EE 330

Lecture 34

Layout of Current Mirrors

Common-Centroid Layouts

High Gain Amplifiers

Cascode Amplifiers

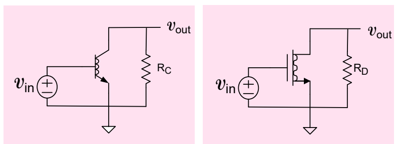
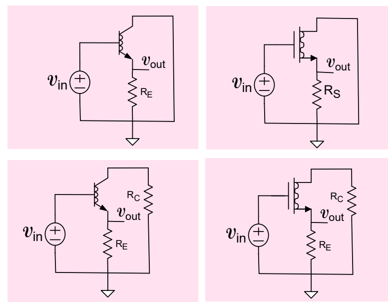
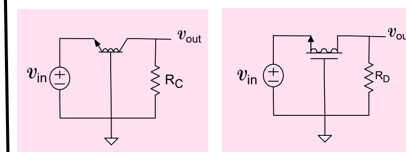
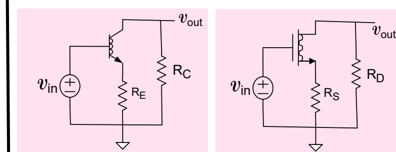
Fall 2025 Exam Schedule

Exam 1	Friday	Sept 26
Exam 2	Friday	October 24
Exam 3	Friday	Nov 21
Final Exam	Monday	Dec 15 12:00 - 2:00 PM

Review From Previous Lecture

Basic Amplifier Application Gain Table

(for low-frequency operation)

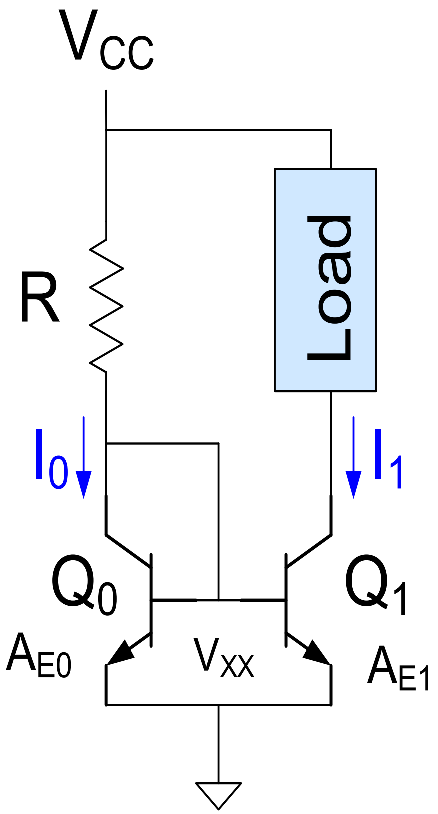
	CE/CS	CC/CD	CB/CG	CEwRE/CSwRS
	BJT / MOS	BJT / MOS	BJT / MOS	BJT / MOS
				
A_V	$-g_mR_C$ BJT: $-\frac{I_{CQ}R_C}{V_t}$ MOS: $-\frac{2I_{DQ}R_D}{V_{EB}}$	$\frac{g_m}{g_m+g_E}$ BJT: $\frac{I_{CQ}R_E}{I_{CQ}R_E+V_t}$ MOS: $\frac{2I_{DQ}R_E}{2I_{DQ}R_E+V_{EB}}$	g_mR_C BJT: $\frac{I_{CQ}R_C}{V_t}$ MOS: $\frac{2I_{DQ}R_C}{V_{EB}}$	$-\frac{R_C}{R_E}$
R_{in}	r_π BJT: $\frac{\beta V_t}{I_{CQ}}$ MOS: ∞	$r_\pi+\beta R_E$ BJT: $\frac{\beta V_t}{I_{CQ}}+\beta R_E \cong \beta R_E$ MOS: ∞	g_m^{-1} BJT: $\frac{V_t}{I_{CQ}}$ MOS: $\frac{V_{EB}}{2I_{DQ}}$	$r_\pi+\beta R_E$ BJT: $\beta\left(\frac{V_t}{I_{CQ}}+R_E\right)\simeq\beta R_E$ MOS: ∞
R_{out}	R_C	g_m^{-1} BJT: $\frac{V_t}{I_{CQ}}$ MOS: $\frac{V_{EB}}{2I_{DQ}}$	R_C	R_C

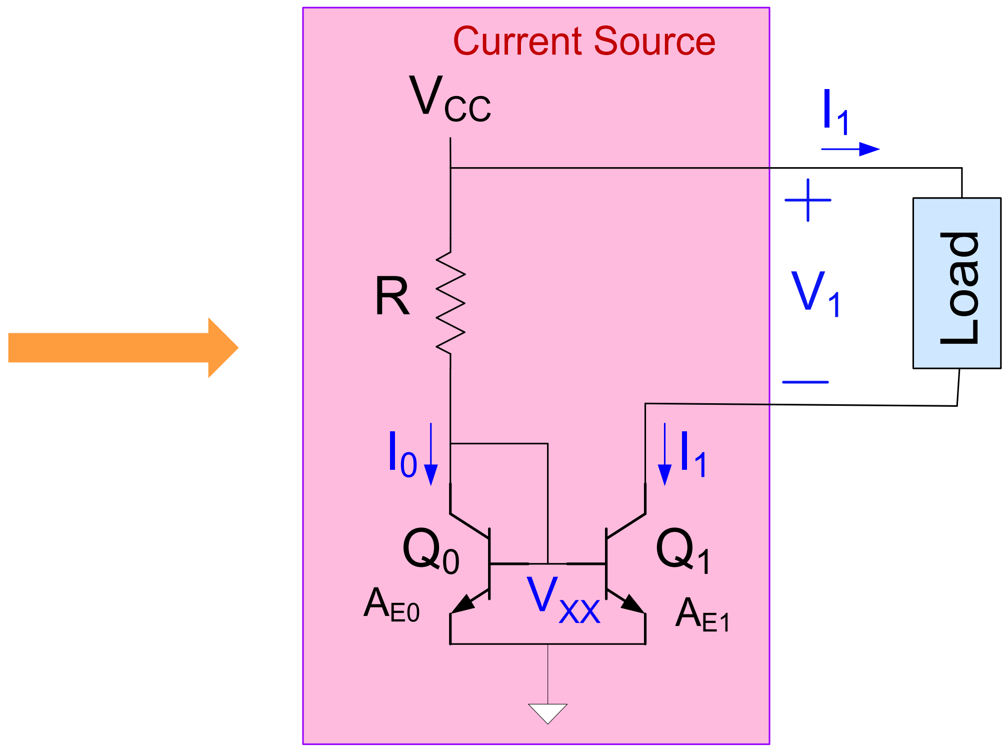
(<u>not</u> two-port models for the four structures)

Can use these equations only when small signal circuit is EXACTLY like that shown !!

Current Sources/Mirrors

Will show circuit in red behaves as a current source

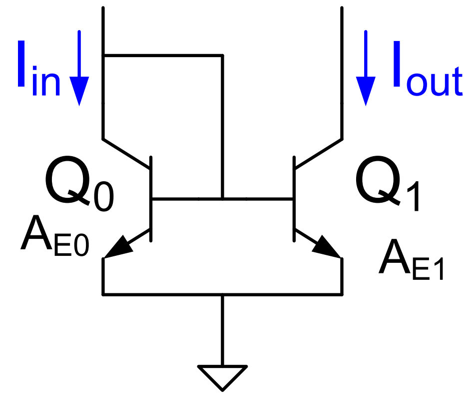




R and Q_0 simply generate voltage V_{XX} in previous circuit

But sensitivity of I_1 is much smaller than using voltage source for generating V_{XX}

Current Sources/Mirrors



npn Current Mirror

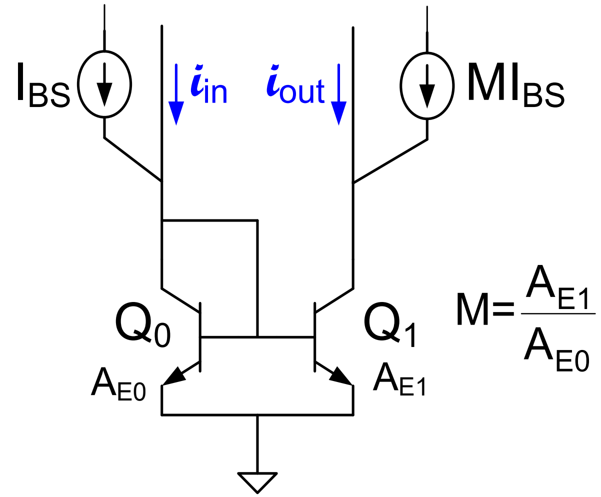
If the base currents are neglected

$$I_{out} = \left[\frac{A_{E1}}{A_{E0}}\right] I_{in}$$

- **Output current linearly dependent on I_{in}**
- **Small-signal and large-signal relationships the same since linear**
- **Serves as a current amplifier**
- **Widely used circuit**

But I_{in} must be positive !

Current Sources/Mirrors



npn current mirror amplifier

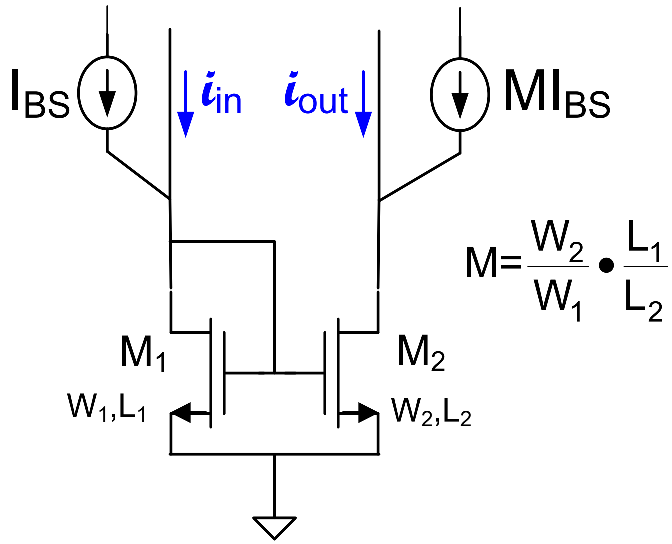
$$i_{out}=\left[\frac{A_{E1}}{A_{E0}}\right]i_{in}$$

Amplifies both positive and negative currents (provided $i_{IN}>-I_{BS}$)

Current amplifiers are easy to build !!

Current gain can be accurately controlled with appropriate layout !!

n-channel current mirror current amplifier

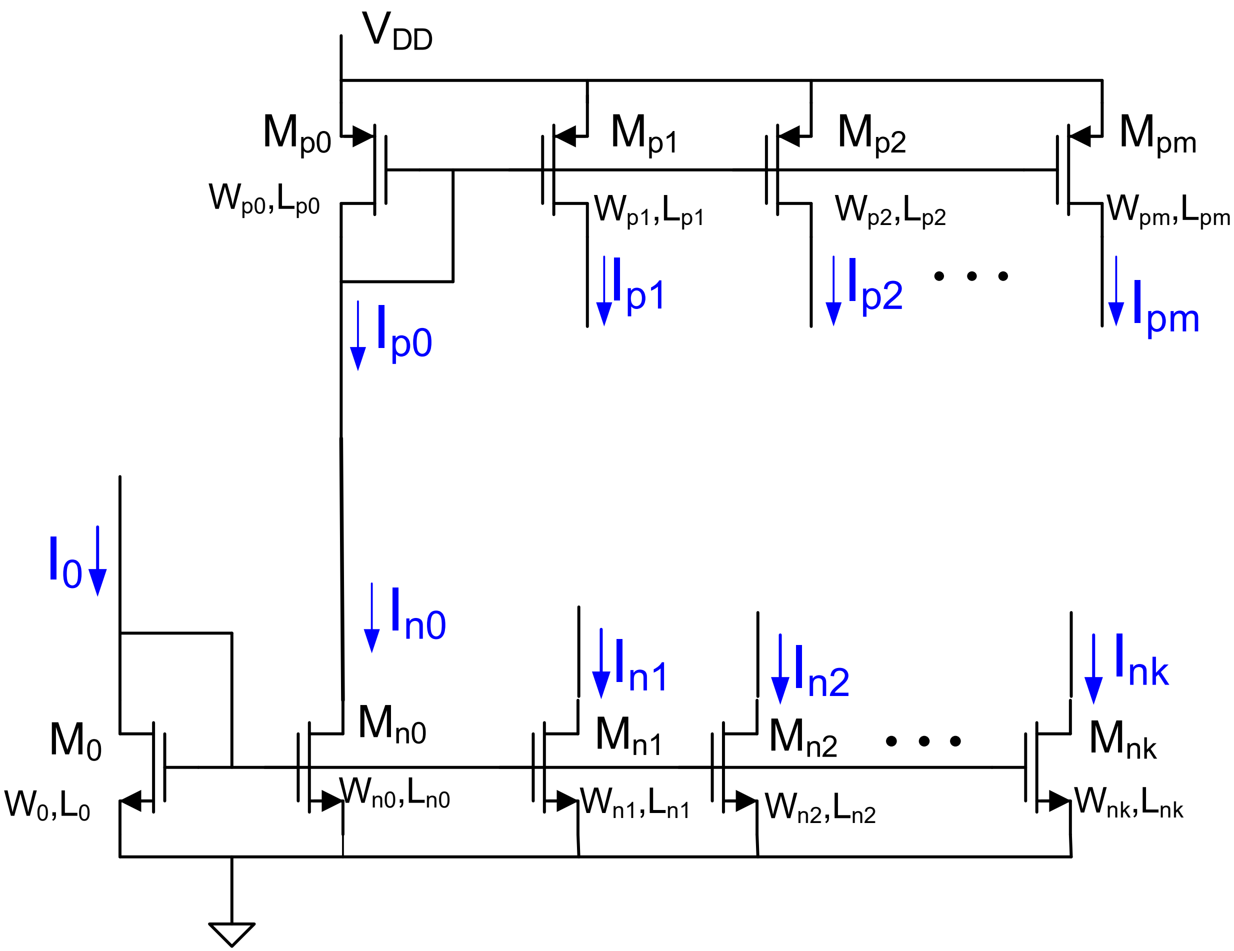


$$i_{out}=\left[\frac{W_2}{W_1}\frac{L_1}{L_2}\right]i_{in}$$

Amplifies both positive and negative currents

Current Sources/Mirrors

multiple sourcing and sinking current outputs



$$I_{pj}=\left[\frac{W_{pj}}{L_{pj}}\bullet\frac{L_{p0}}{W_{p0}}\right]MI_0$$

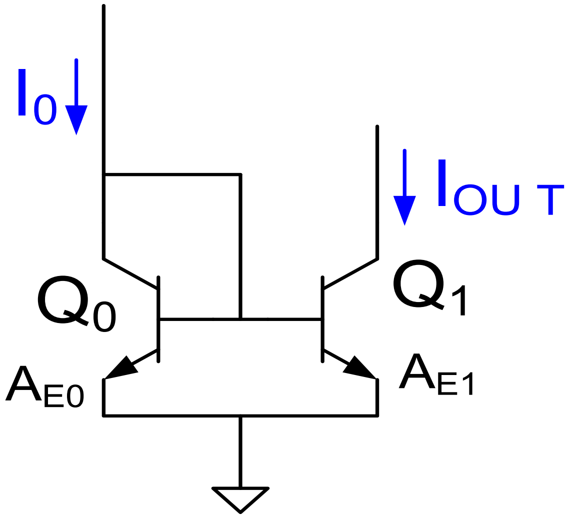
$$M=\left[\frac{W_{n0}}{L_{n0j}}\bullet\frac{L_0}{W_0}\right]$$

$$I_{nj}=\left[\frac{W_{nj}}{L_{nj}}\bullet\frac{L_0}{W_0}\right]I_0$$

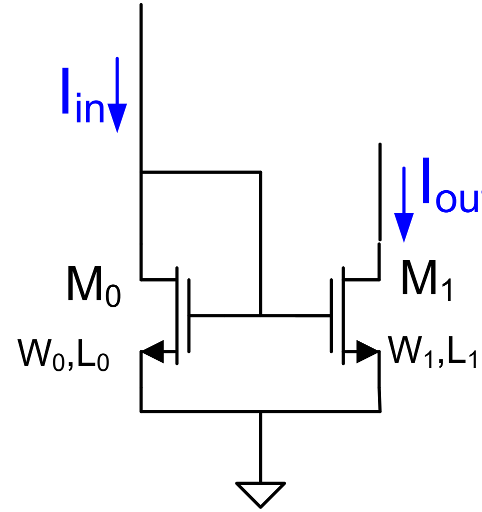
m and k may be different

Often M=1

Current Sources/Mirrors Summary



npn Current Mirror



n-channel Current Mirror

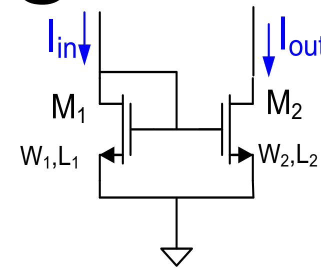
$$I_{out} = \left[\frac{A_{E1}}{A_{E0}}\right] I_{in}$$

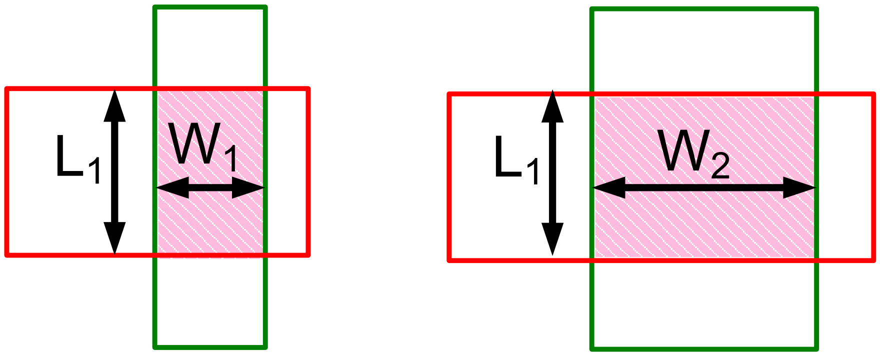
$$I_{out} = \left[\frac{W_1}{W_0}\frac{L_0}{L_1}\right] I_{in}$$

- Current mirror gain <u>can</u> be accurately controlled !
- Layout is important to get accurate gain (for both MOS and BJT)

Layout of Current Mirrors

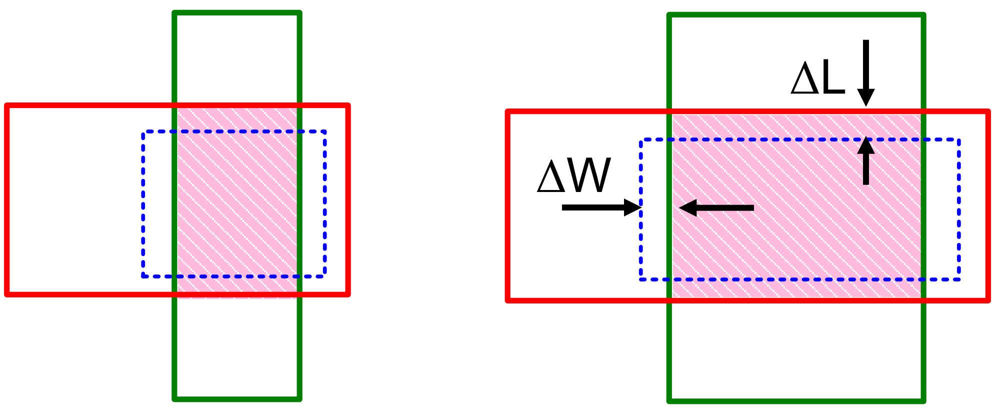
Example with M = 2





Standard layout

$$M=\left[\frac{W_2}{W_1}\frac{L_1}{L_2}\right]$$



$$M=\left[\frac{W_2+2\Delta W}{W_1+2\Delta W}\bullet\frac{L_1+2\Delta L}{L_2+2\Delta L}\right]$$

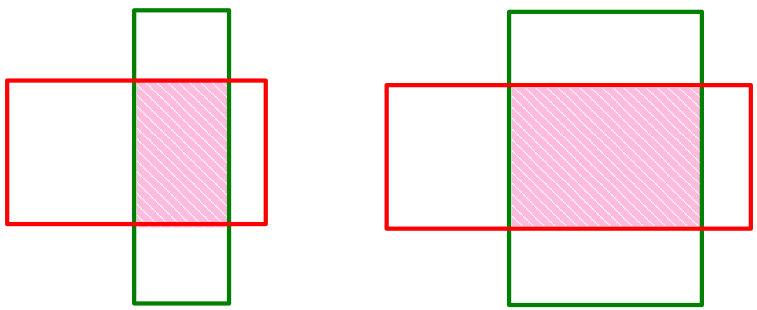
$$M=\left[\frac{2W_1+2\Delta W}{W_1+2\Delta W}\bullet\frac{L_1+2\Delta L}{L_1+2\Delta L}\right]\neq 2$$

Gate area after fabrication depicted

ΔL and ΔW can be positive or negative

Layout of Current Mirrors

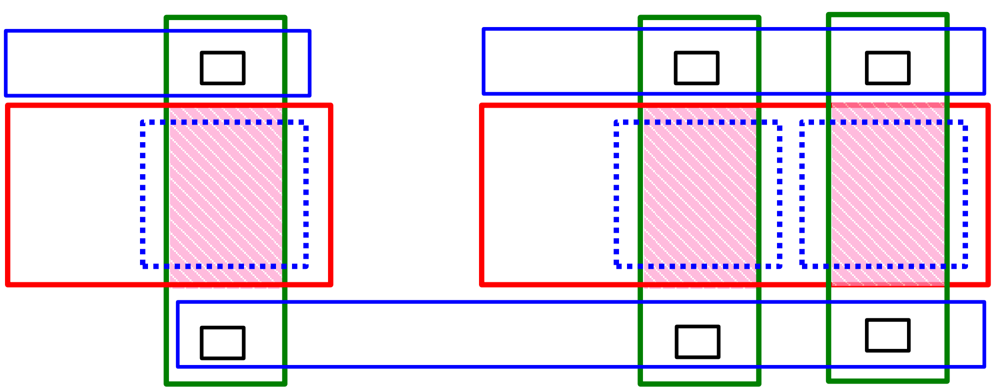
Example with M = 2



$$M = \left[\frac{W_2}{W_1} \frac{L_1}{L_2} \right]$$

$$M = \left[\frac{2W_1 + 2\Delta W}{W_1 + 2\Delta W} \bullet \frac{L_1 + 2\Delta L}{L_1 + 2\Delta L} \right] \neq 2$$

Standard layout

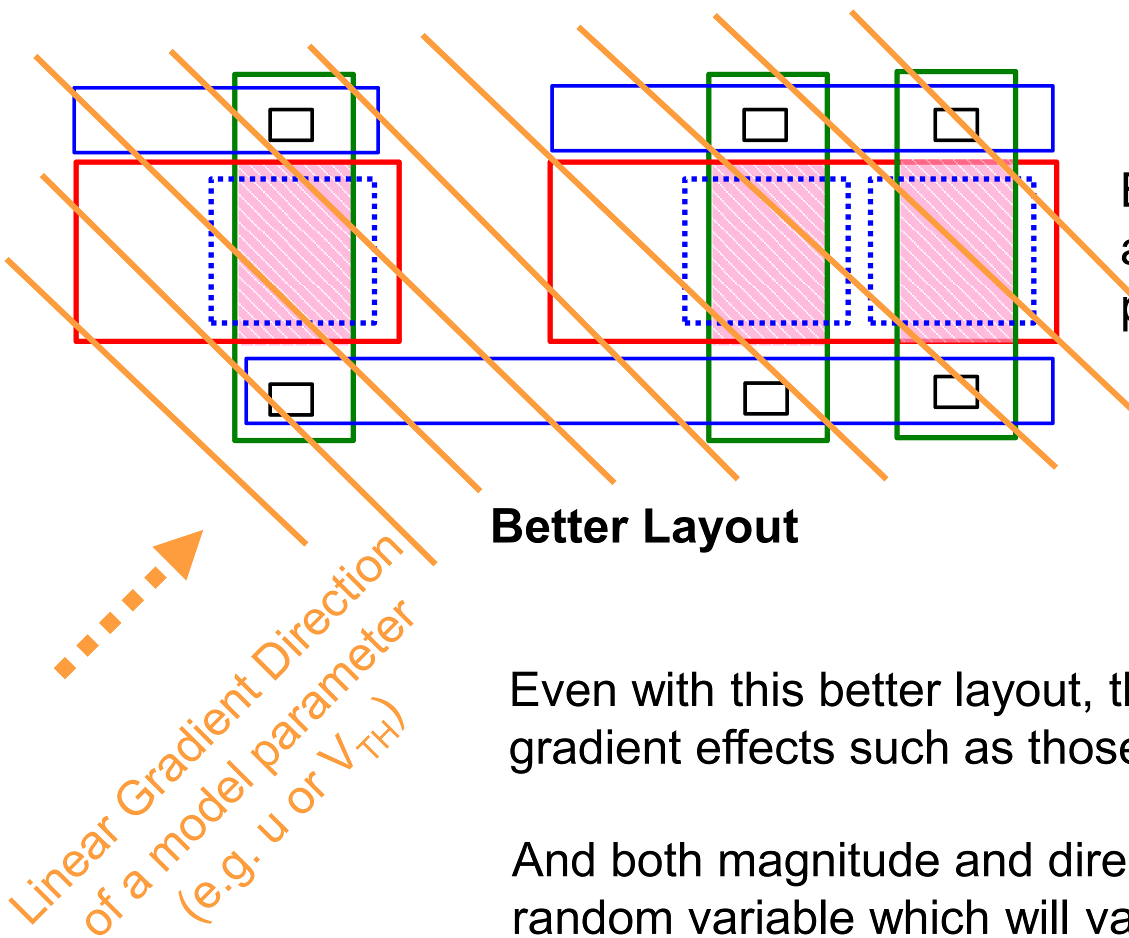


$$M = \left[\frac{2W_1 + 4\Delta W}{W_1 + 2\Delta W} \bullet \frac{L_1 + 2\Delta L}{L_1 + 2\Delta L} \right] = 2$$

Better Layout

Layout of Current Mirrors

Example with M = 2



Better Layout

$$M=\left[\frac{2W_1+4\Delta W}{W_1+2\Delta W}\bullet\frac{L_1+2\Delta L}{L_1+2\Delta L}\right]=2$$

But this analysis was based upon assumption of matching of process parameters

$$I_{in}=\frac{\mu_0 C_{OX} W_0}{2L_0}\left(V_{GS0}-V_{T0}\right)^2$$

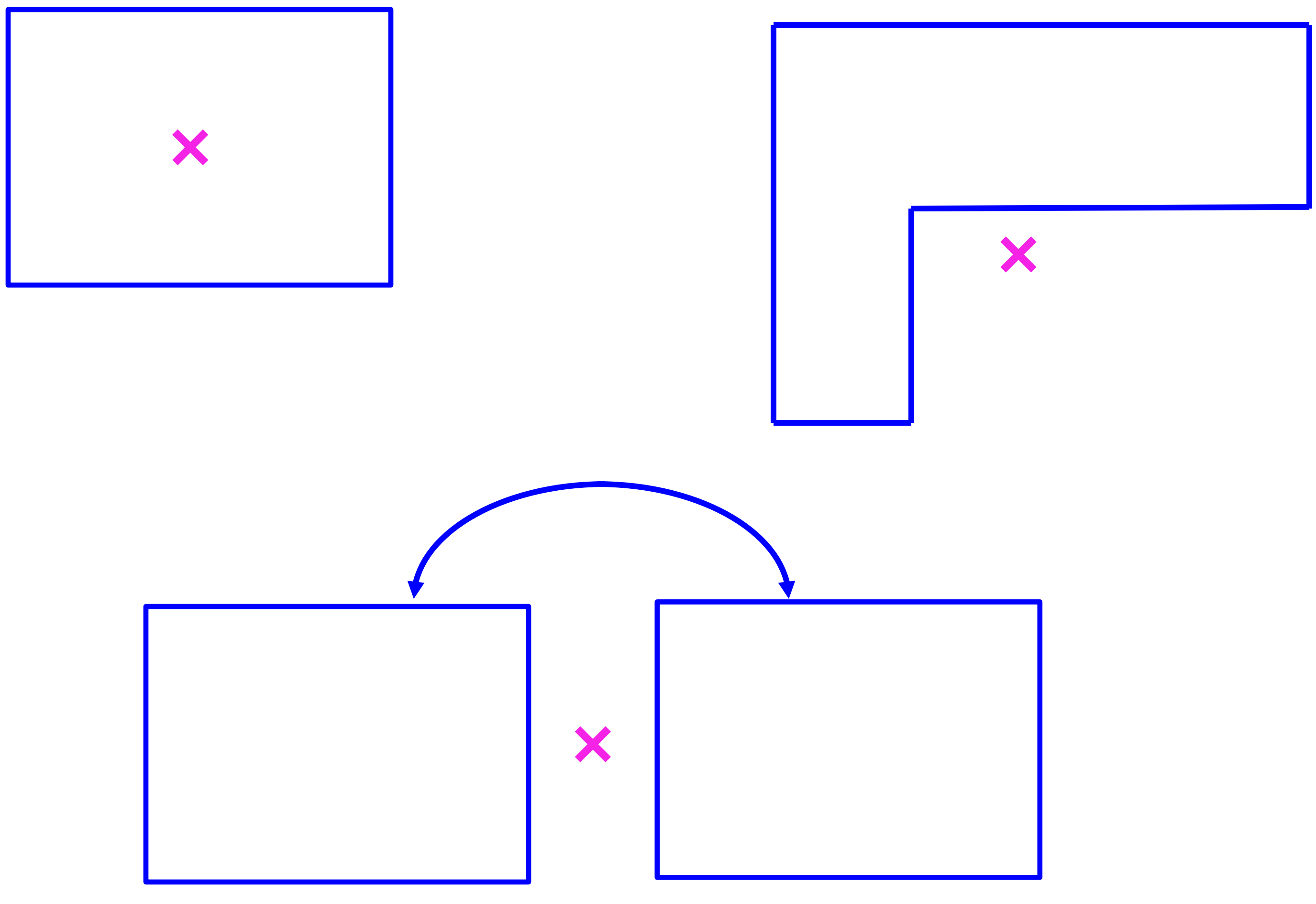
$$I_{out}=\frac{\mu_1 C_{OX} W_1}{2L_1}\left(V_{GS1}-V_{T1}\right)^2$$

Even with this better layout, the current ratio will not be 2 if gradient effects such as those depicted here are shown

And both magnitude and direction of gradient effects are a random variable which will vary across a die

Centroid and Common Centroid

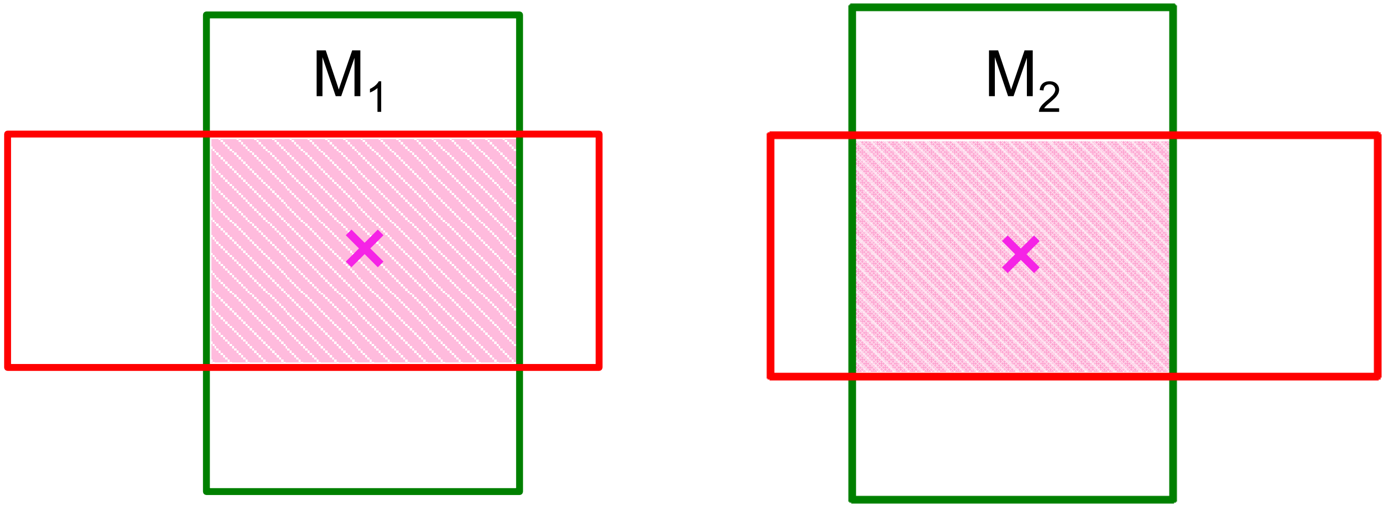
× Denotes Geometric Centroid



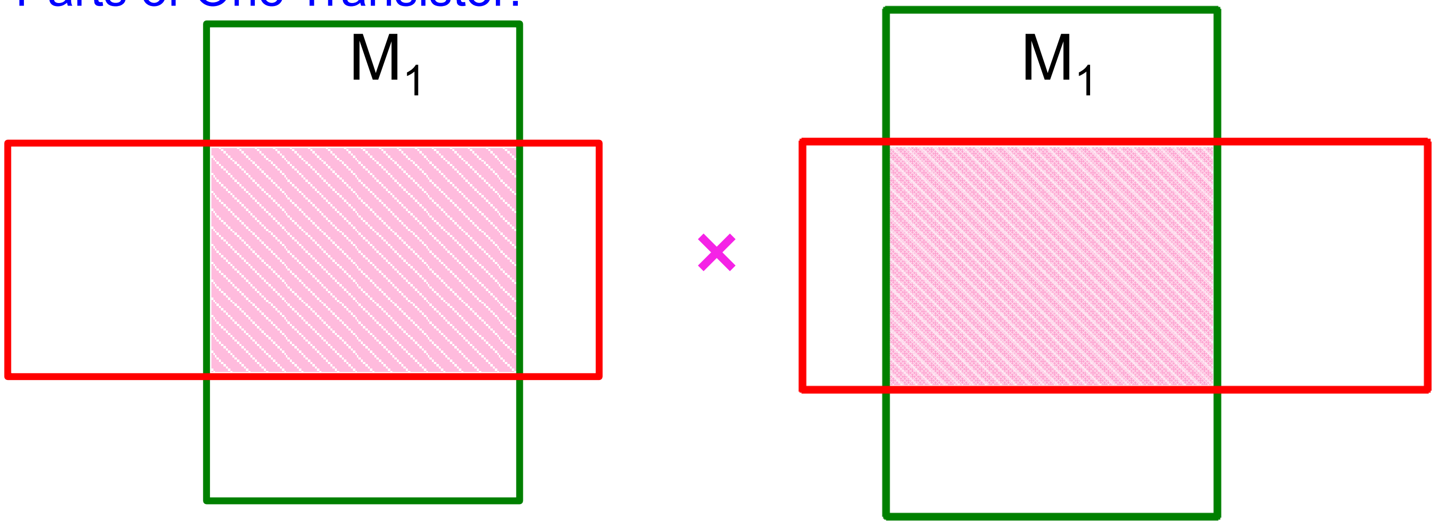
Centroid and Common Centroid

Geometric Centroids of Channel

Two Transistors:

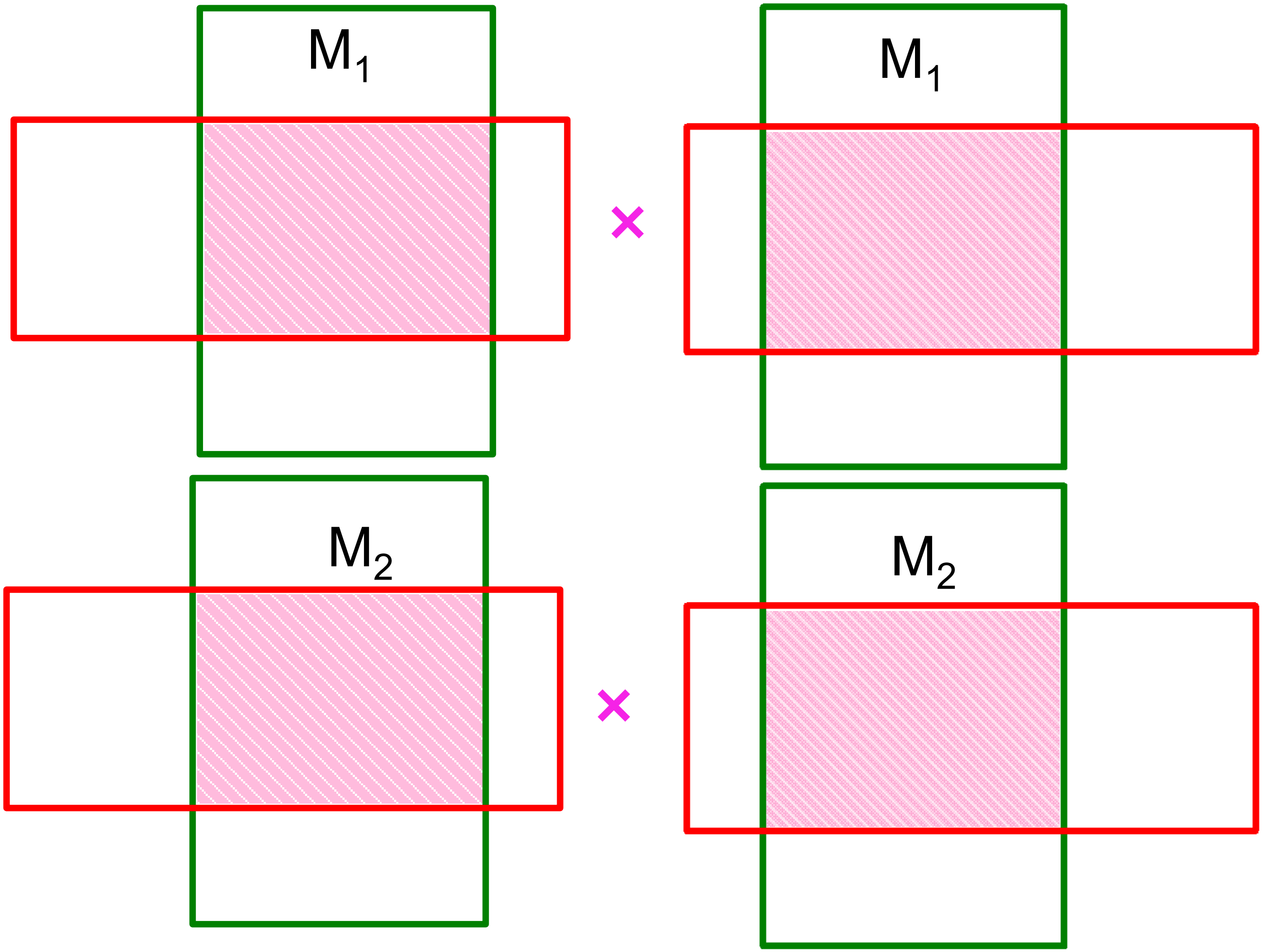


Two Parts of One Transistor:



Centroid and Common Centroid

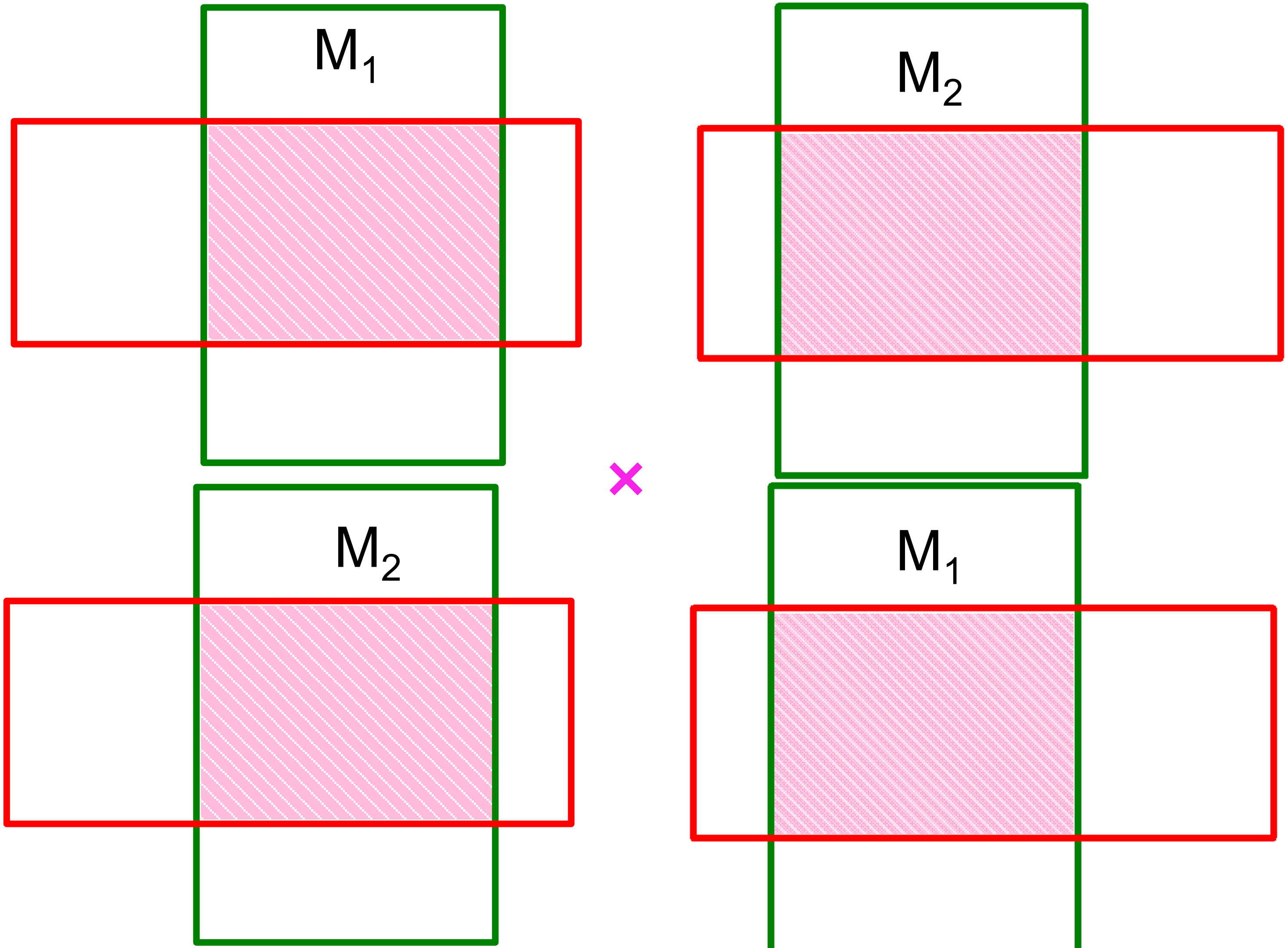
Two Transistors each with two parts:



Centroid and Common Centroid

Common Centroid for Ideally Matched Devices

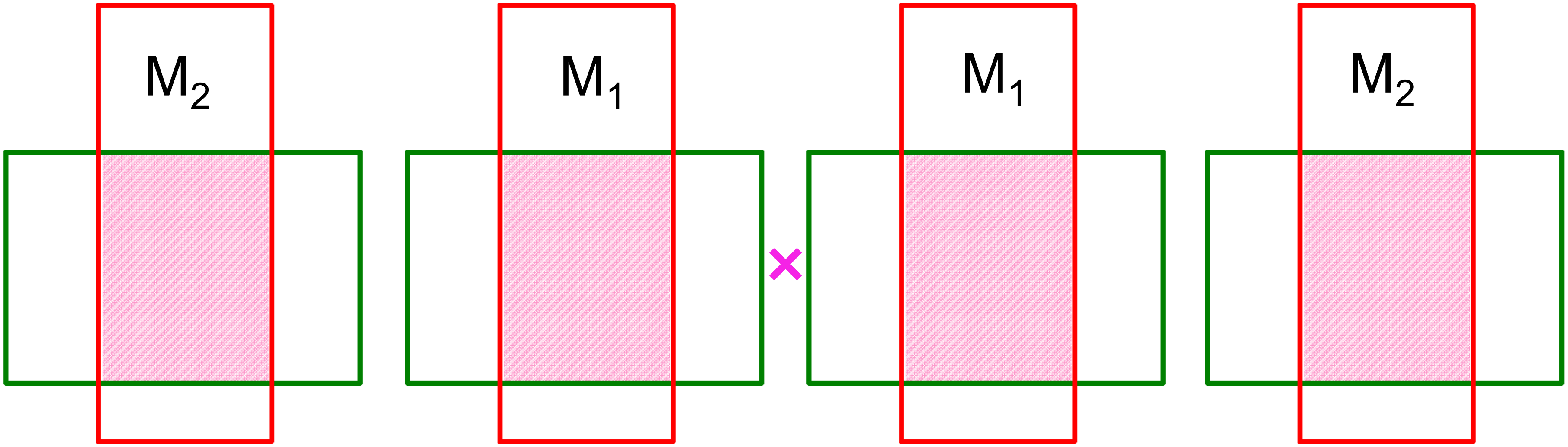
Two Transistors each with two parts:



Centroid and Common Centroid

Common Centroid for Matched Devices

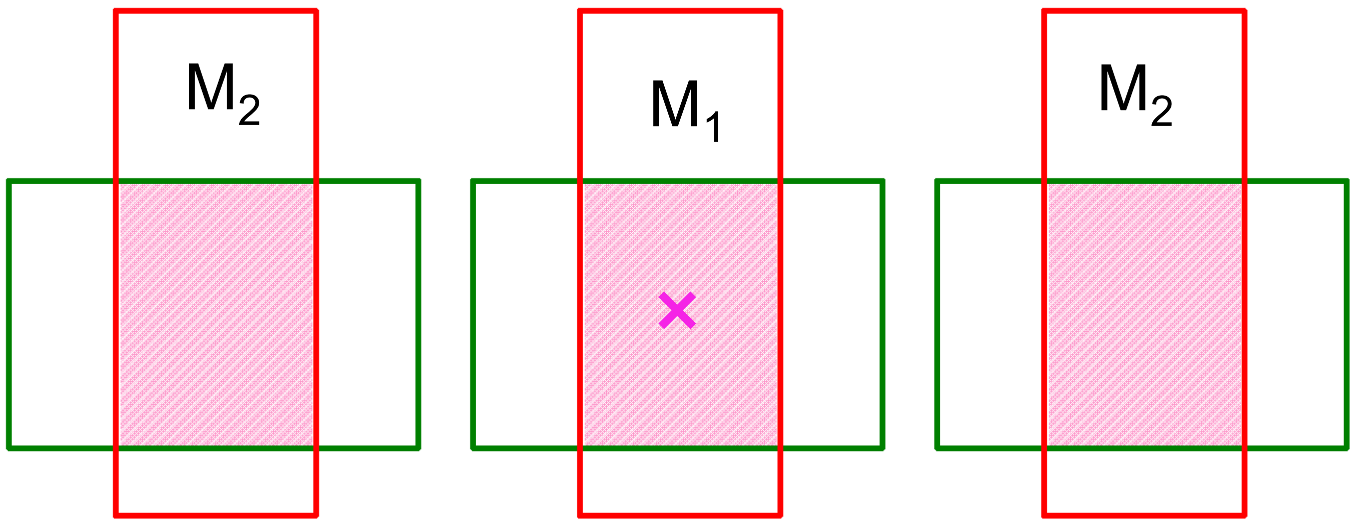
Two Transistors each with two parts:



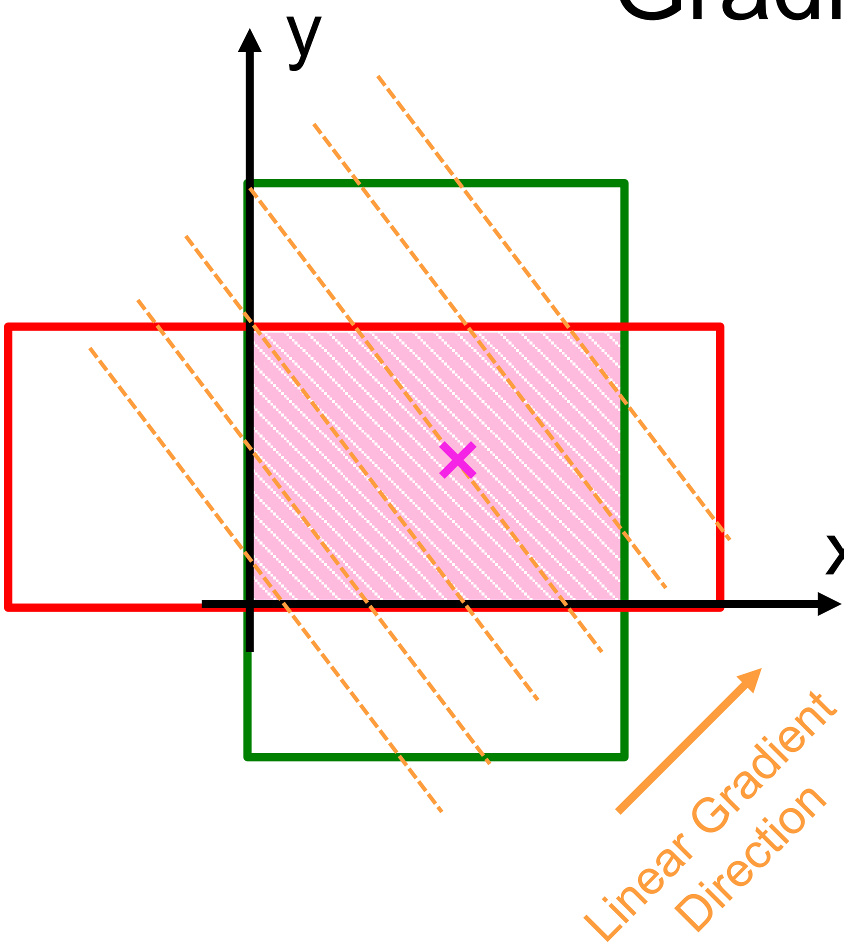
Centroid and Common Centroid

Common Centroid for Ratioed Devices $M = \frac{W_2}{W_1}\frac{L_1}{L_2} = 2$

Two Transistors with different effective widths:



Gradient



Threshold voltage dependent upon position

$V_{TH}(x,y)$

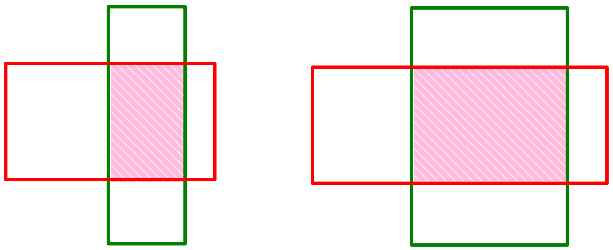
- Significant changes in threshold voltage can occur due to gradient effects
- This can seriously degrade matching in matching-critical circuits
- Gradients in key parameters (V_{TH}, μC_{OX}) usually nearly linear

- If the threshold voltage of a transistor changes with position, it can be reasonably accurately modeled with an "equivalent" threshold voltage
- For linear gradient, $V_{THEQ}=V_{TH}(X_C,Y_C)$

× : (X_C,Y_C)

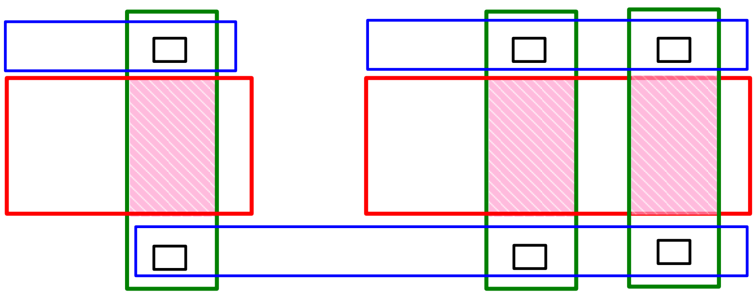
Layout of Current Mirrors

Example with M = 2



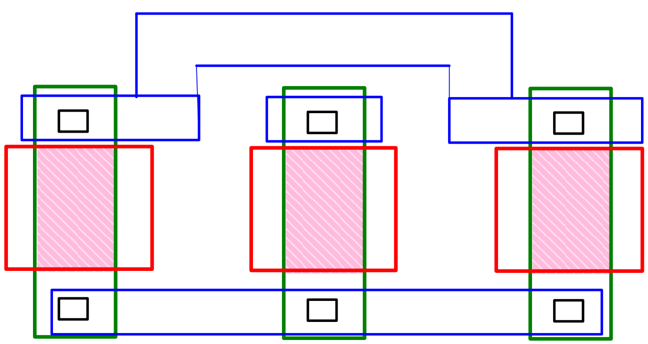
Standard layout

$$M=\left[\frac{W_2}{W_1}\frac{L_1}{L_2}\right]$$



Better Layout

$$M=\left[\frac{2W_1+4\Delta W}{W_1+2\Delta W}\bullet\frac{L_1+2\Delta L}{L_1+2\Delta L}\right]=2$$



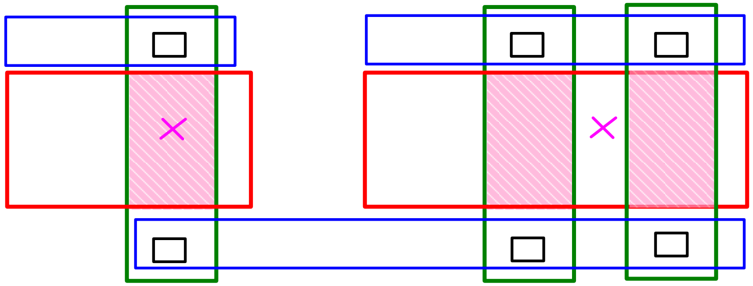
Even Better Layout

$$M=\left[\frac{2W_1+4\Delta W}{W_1+2\Delta W}\bullet\frac{L_1+2\Delta L}{L_1+2\Delta L}\right]=2$$

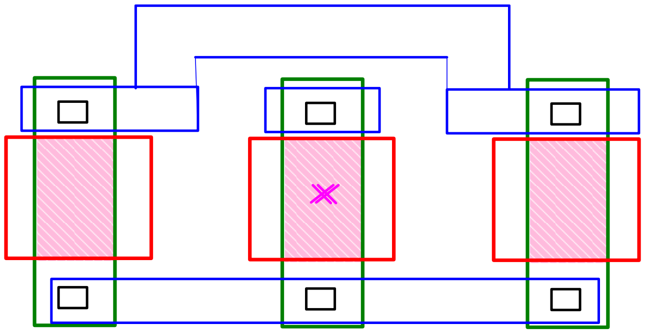
- **This is termed a common-centroid layout**

Layout of Matching-Critical Circuits

Example with M = 2



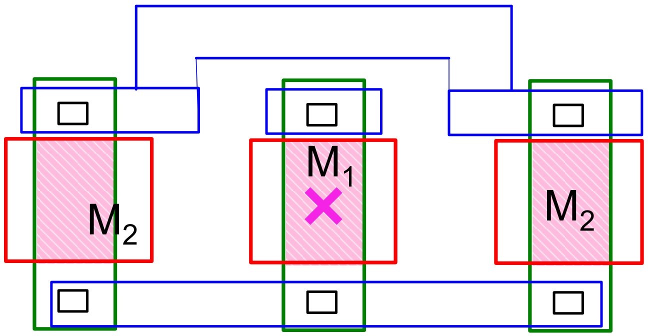
Better Layout



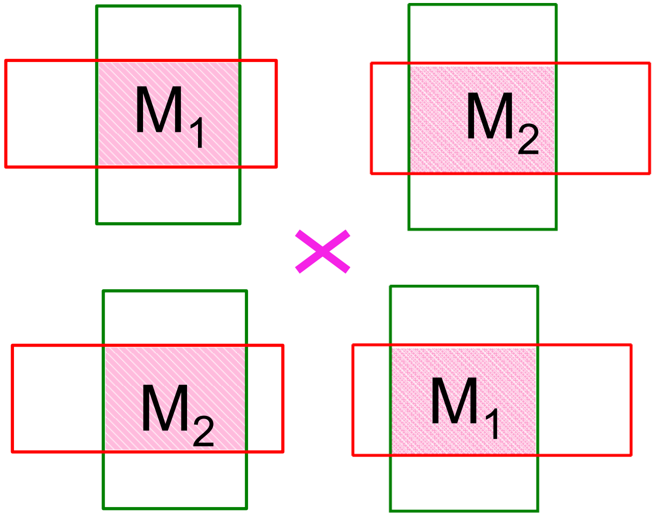
Common-centroid Layout

Theorem: **Linear gradient mismatch eliminated with common-centroid layout !**

Common-Centroid Layouts



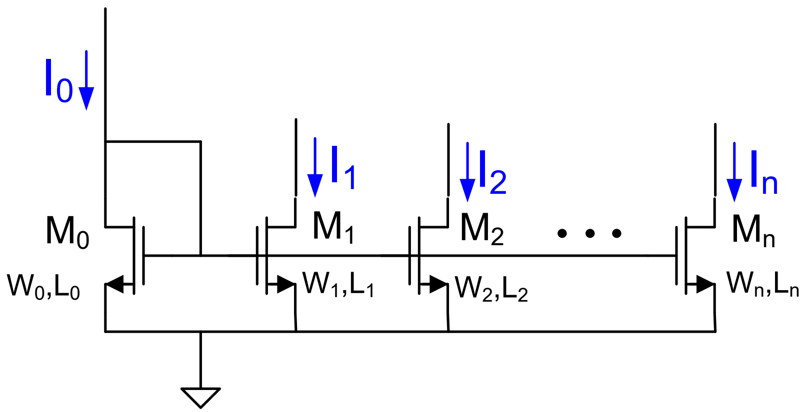
$$M = \left[\frac{2W_1}{W_1} \bullet \frac{L_1}{L_1} \right] = 2$$

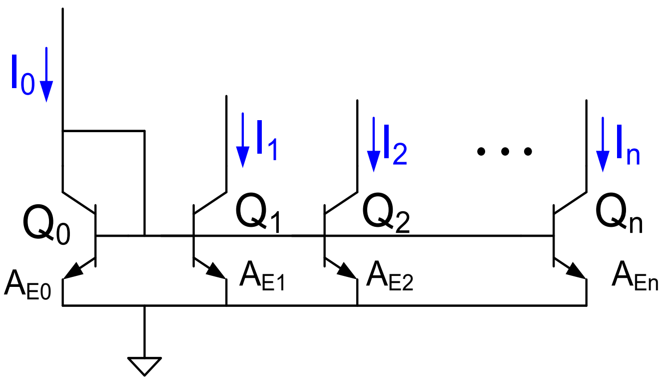


$$M = \left[\frac{2W_1}{2W_1} \bullet \frac{L_1}{L_1} \right] = 1$$

- Individual transistors in matching-critical circuits often decomposed into multiple parallel unary devices connected in parallel and placed with common centroid
- Common-Centroid layout approach widely used to minimize (ideally cancel) linear gradient effects in matching-critical circuits
- Applications extend well beyond current mirrors
- More than 2 devices can share a common centroid

Current Sources/Mirrors

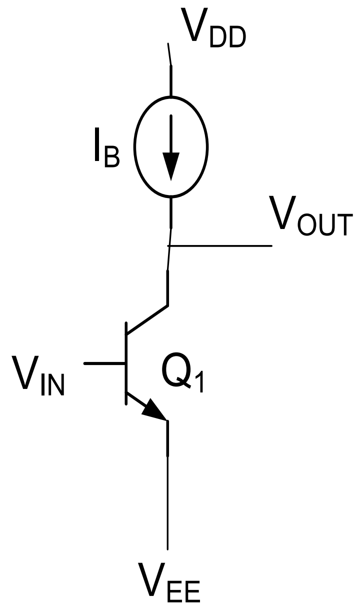




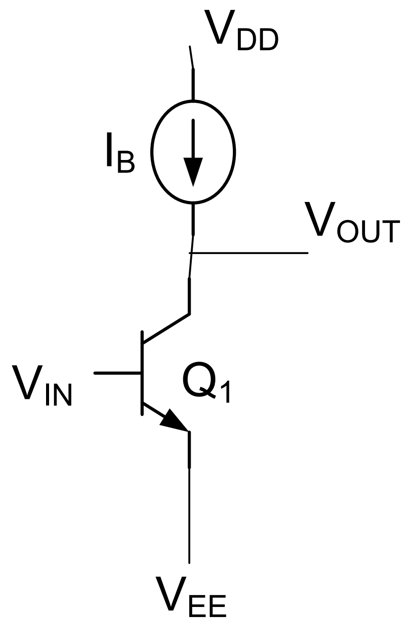
If I_0 is practically generated (it can be), now have available a large number of accurate current sources or sinks that can be used for biasing and for other purposes on chip !

High-gain amplifier

Will now return to discussion of high gain amplifiers



High-gain amplifier



$$A_V \cong -8000$$

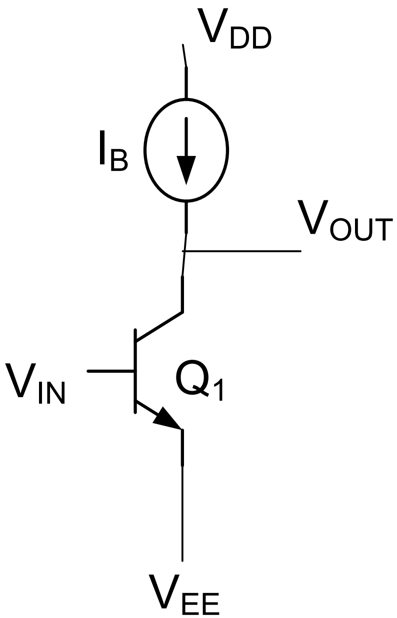
Why are we interested in high-gain amplifiers?

- High gain amplifiers typically have some very undesirable properties

  Nonlinear, gain highly dependent upon process variations and temperature, frequency response poor, noisy, ….

- So we can build feedback amplifiers !!

High-gain amplifier



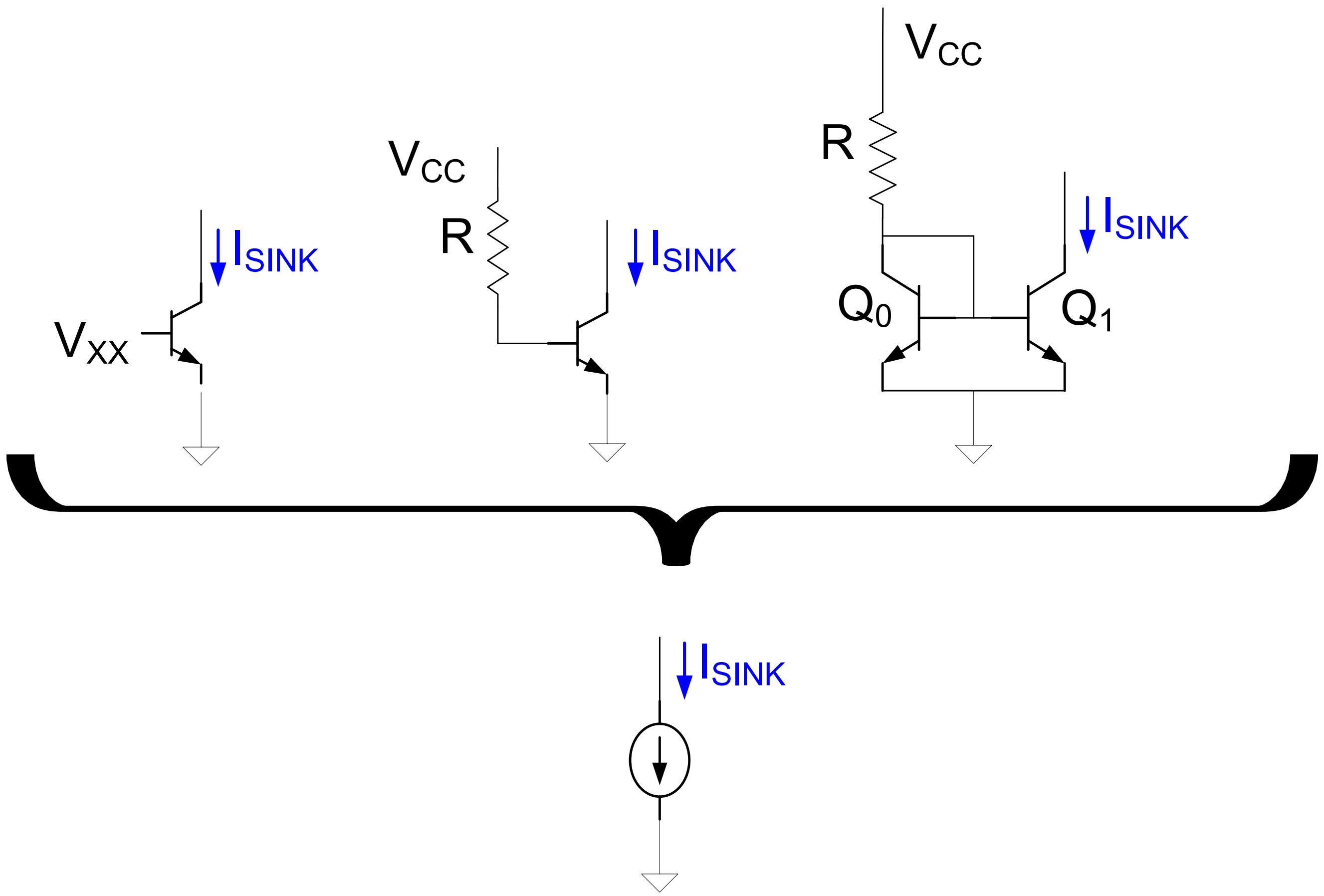
$$A_V \cong -8000$$

→ How can we build the current source?

What is the small-signal model of an actual current source?

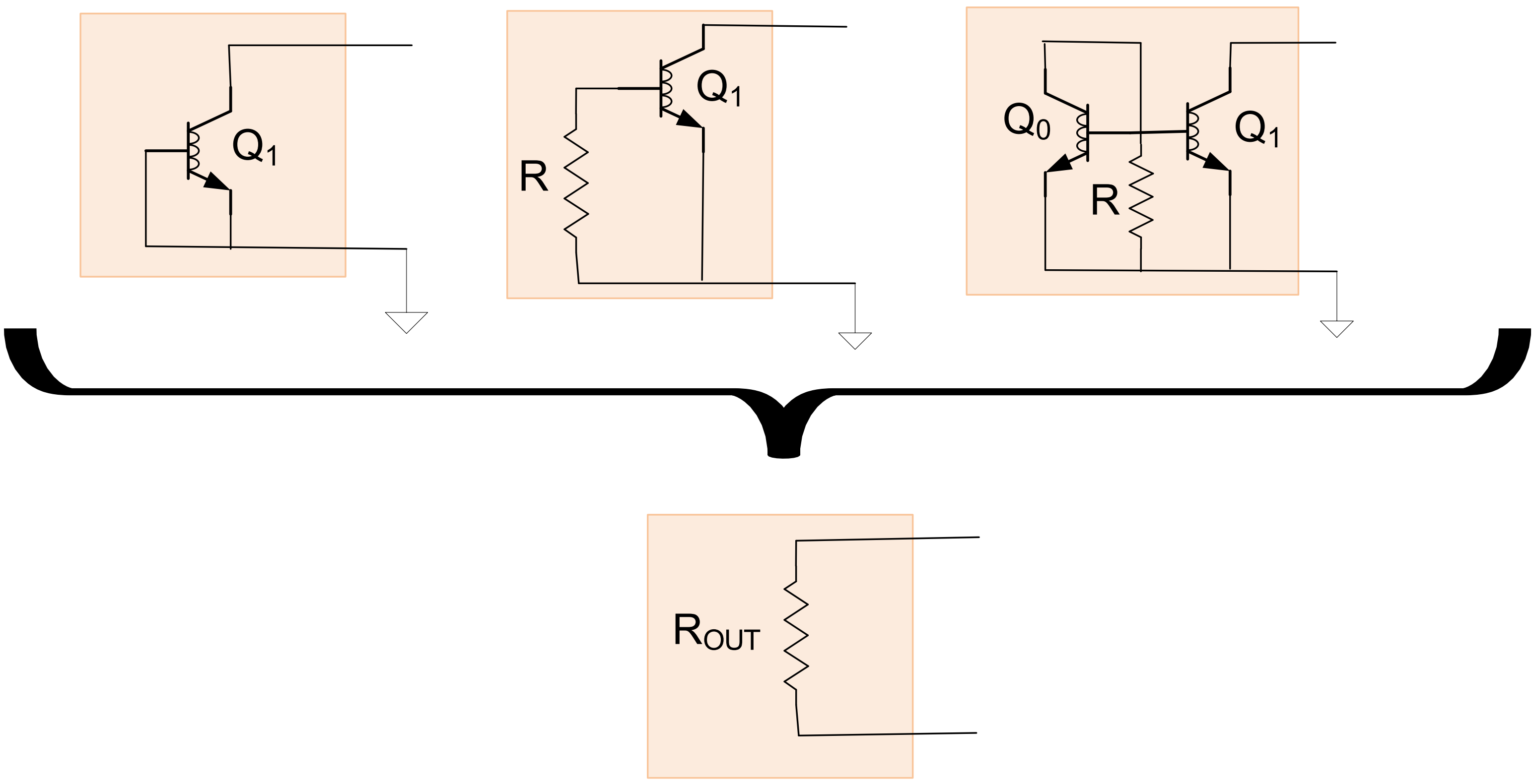
How can we build current source (or sink)?

3 of many ways shown for bipolar process



How can we build current source (or sink)?

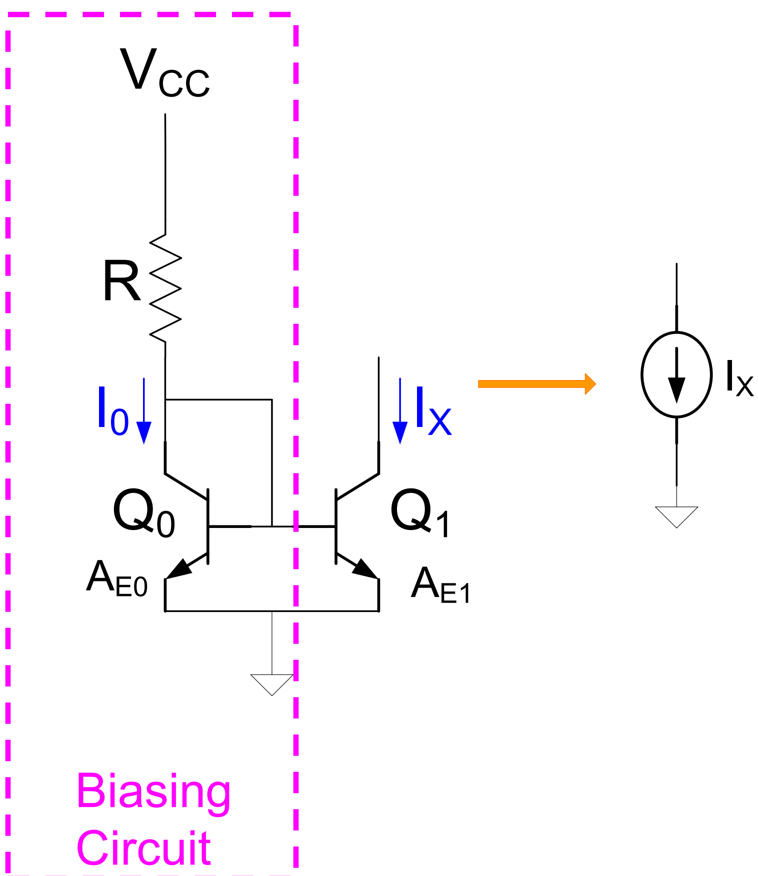
Note: All are small-signal one-ports and equivalent to a resistor R_{OUT}



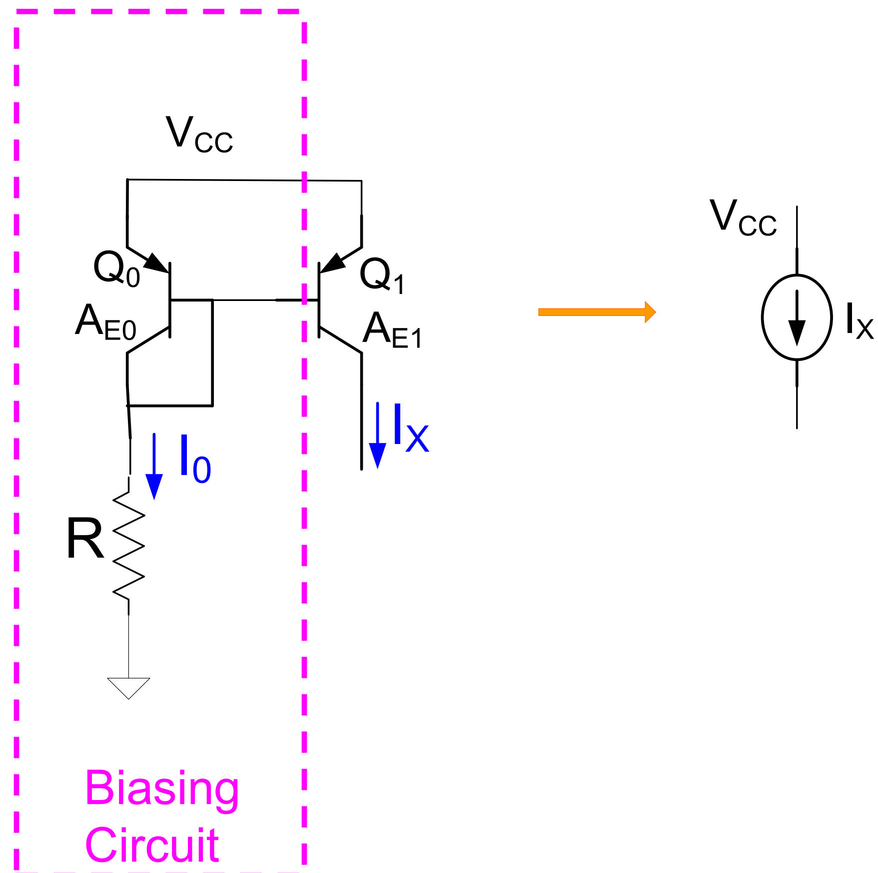
Basic Current Sources and Sinks

Consider as an example:

Bipolar Mirror-Based Current Sink



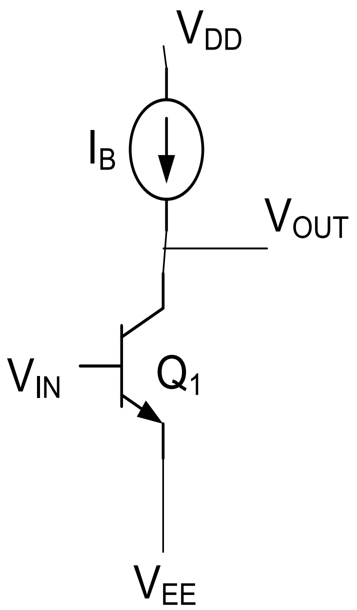
Bipolar Mirror-Based Current Source

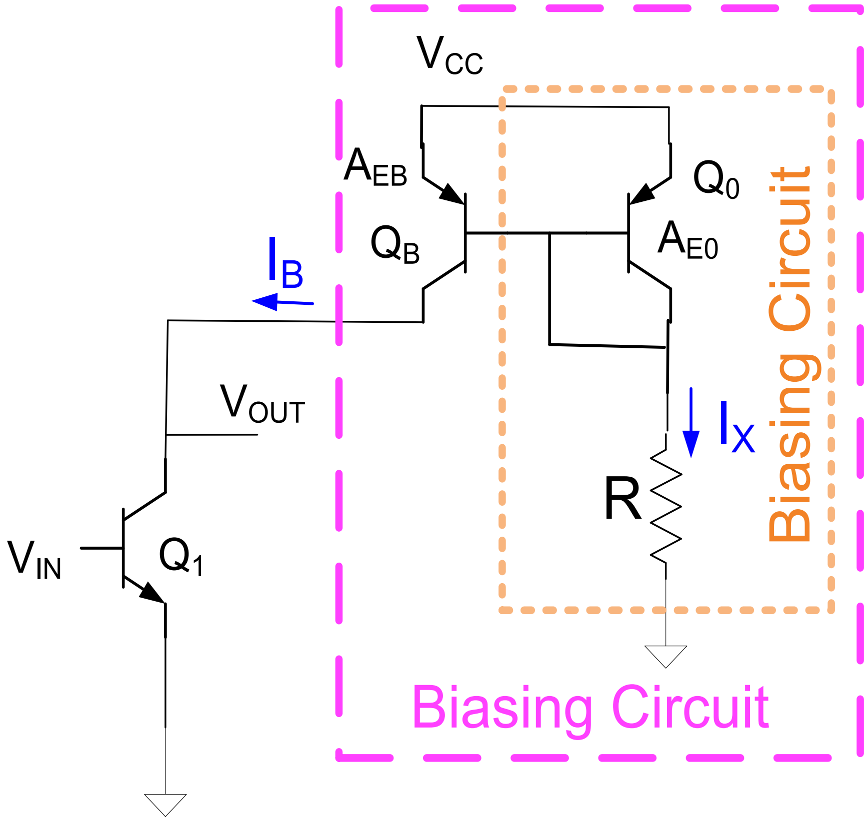


Biasing circuit uses same V_{CC} as amplifier and no other independent sources

High-gain amplifier

Consider as an example:

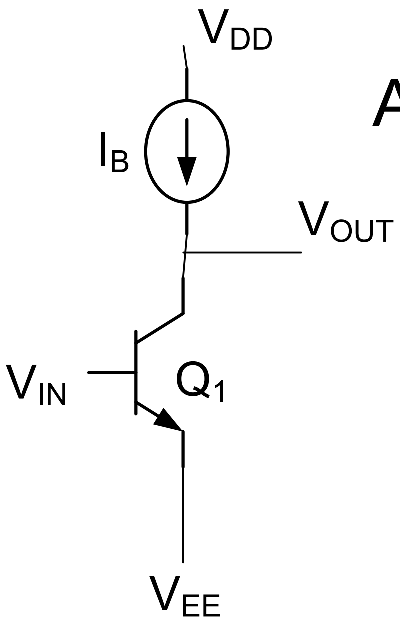




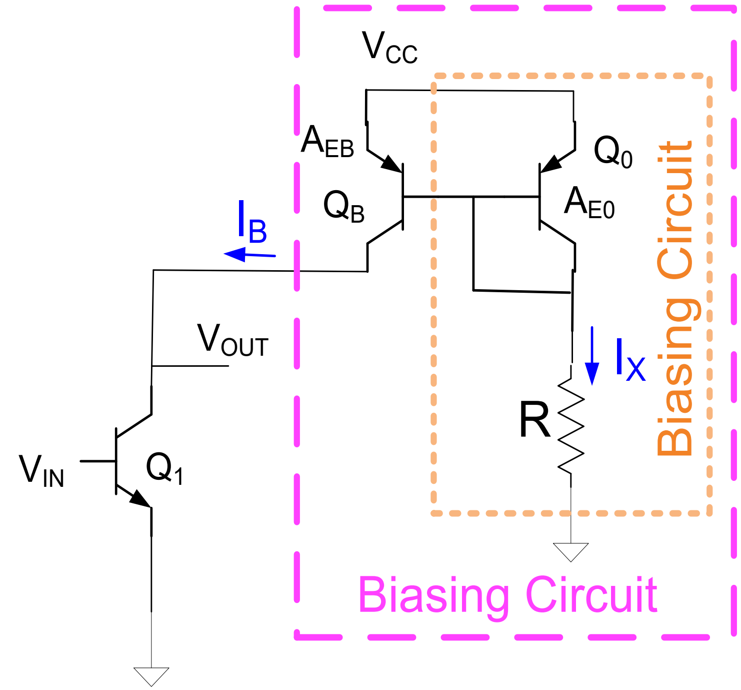
- Bias circuitry for biasing circuit requires only a single independent dc voltage source, resistor, and BJT !
- <u>Incremental</u> overhead for each additional current output is only one transistor, Q_B

High-gain amplifier

Consider as an example:



$$A_V \cong -8000$$



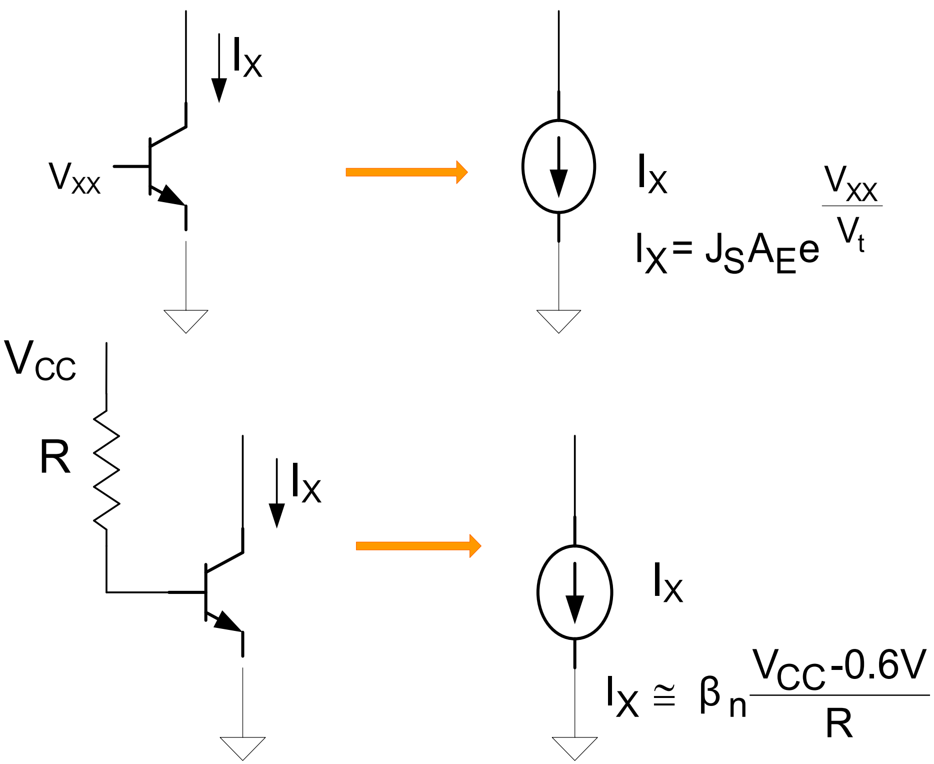
How can we build the current source?

→ What is the small-signal model of an actual current source?

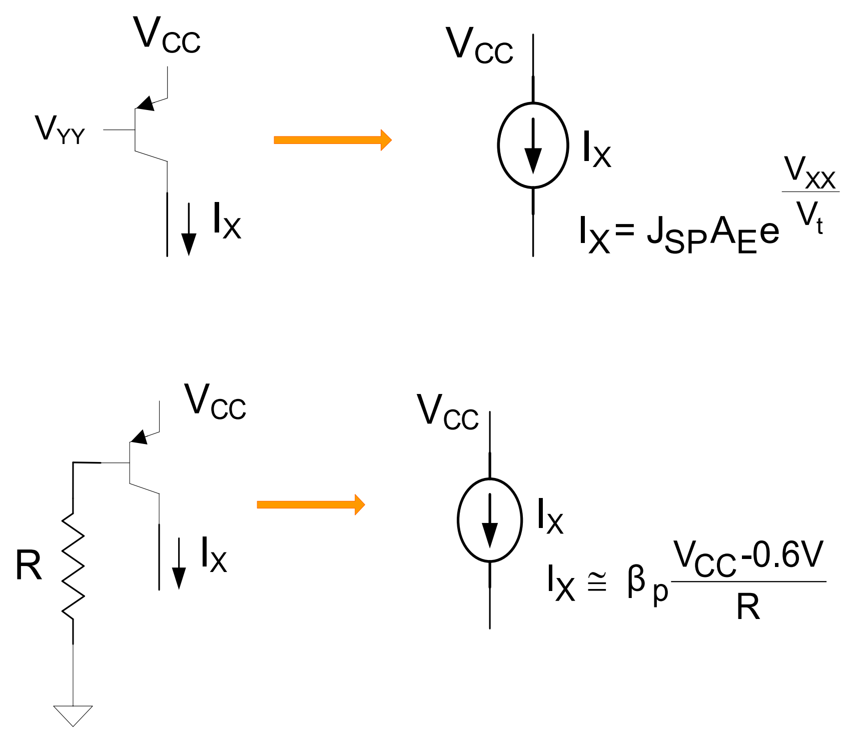
Basic Current Sources and Sinks

DC Models of Basic Bipolar Sinks and Sources

Basic Bipolar Current Sinks



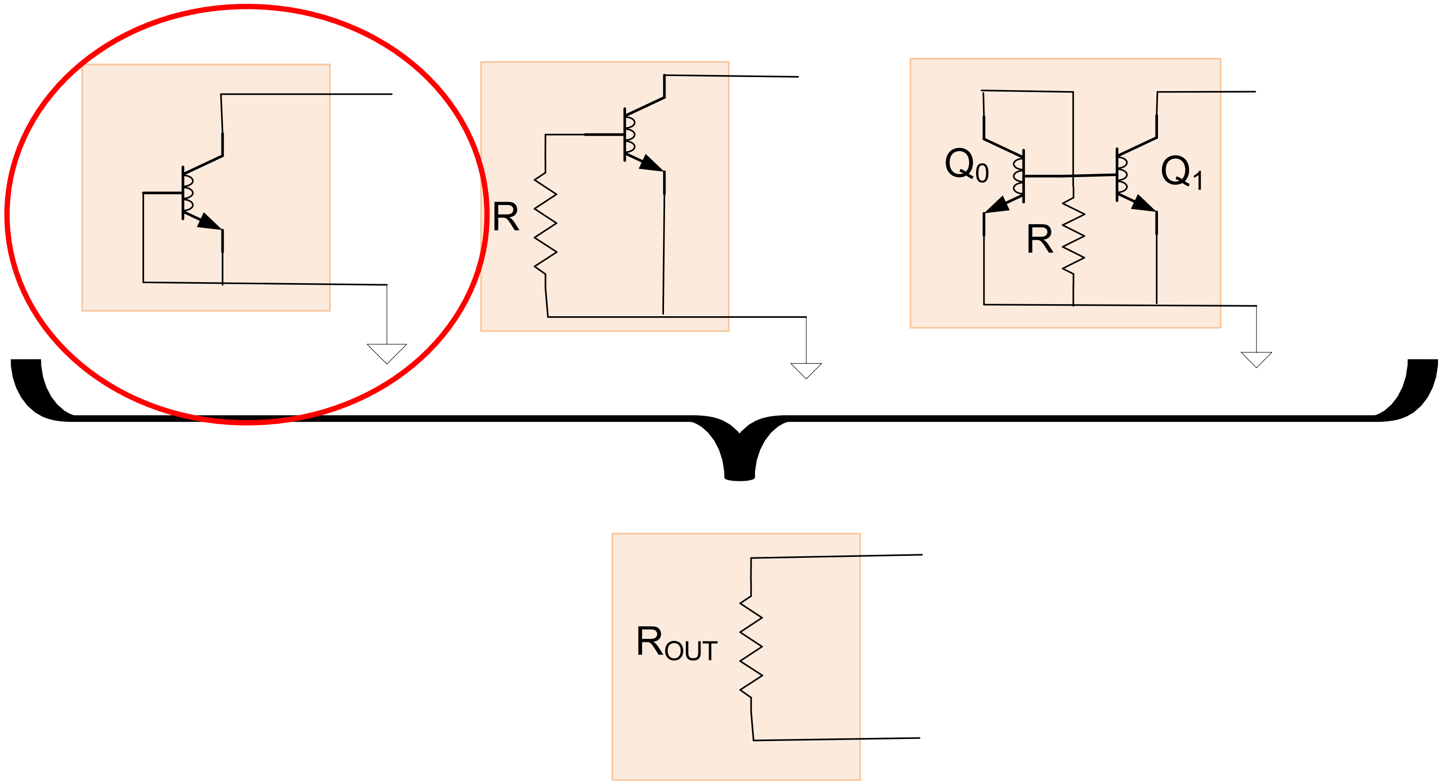
Basic Bipolar Current Sources



- Very practical methods for biasing the BJTs (or MOSFETs) can be used
- Current Mirrors often used for generating sourcing and sinking currents
- Can think of biasing transistors with V_{XX} and V_{YY} in these current sources

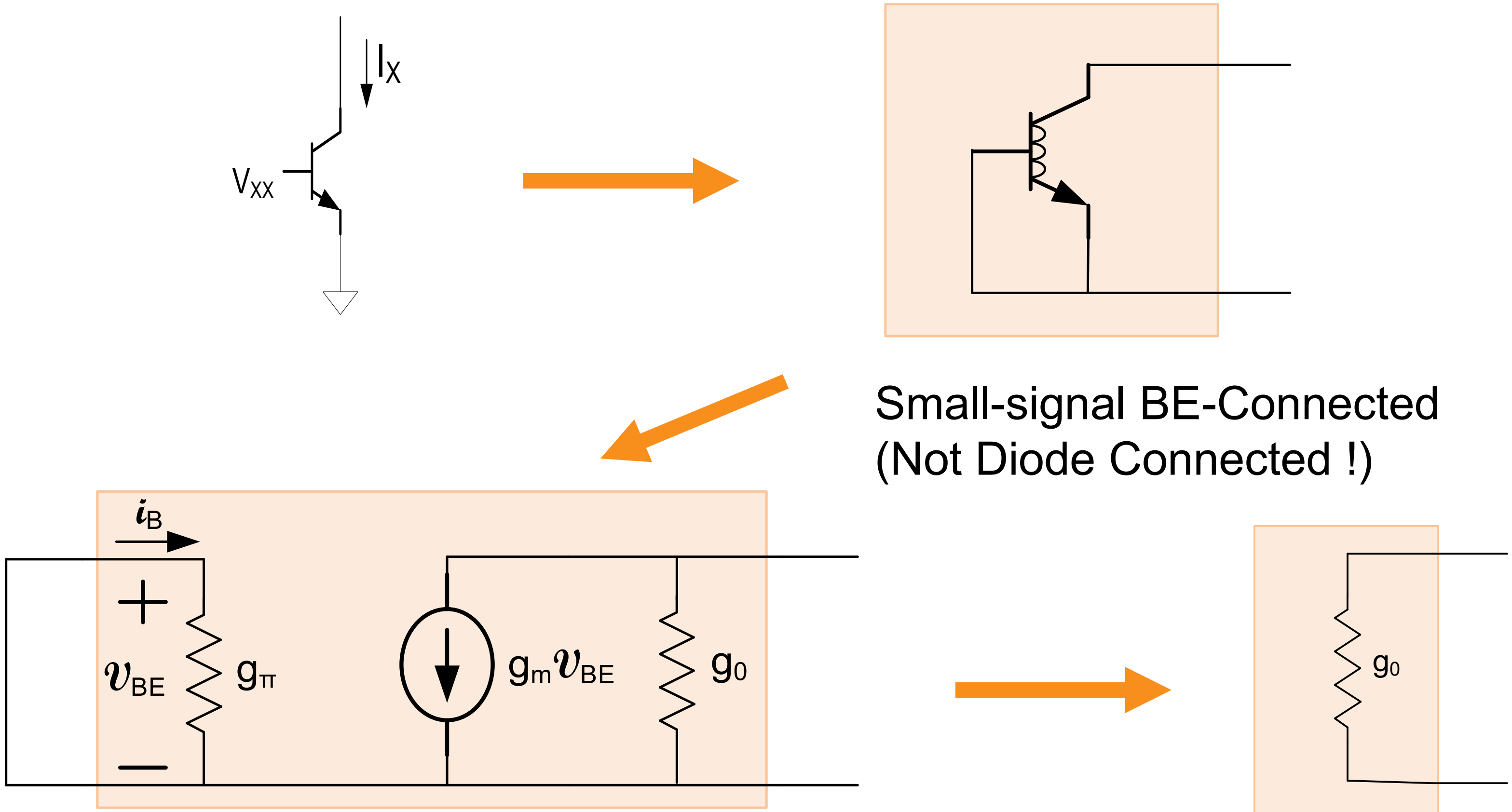
Basic Current Sources and Sinks

Small-signal Model of BJT Current Sinks and Sources



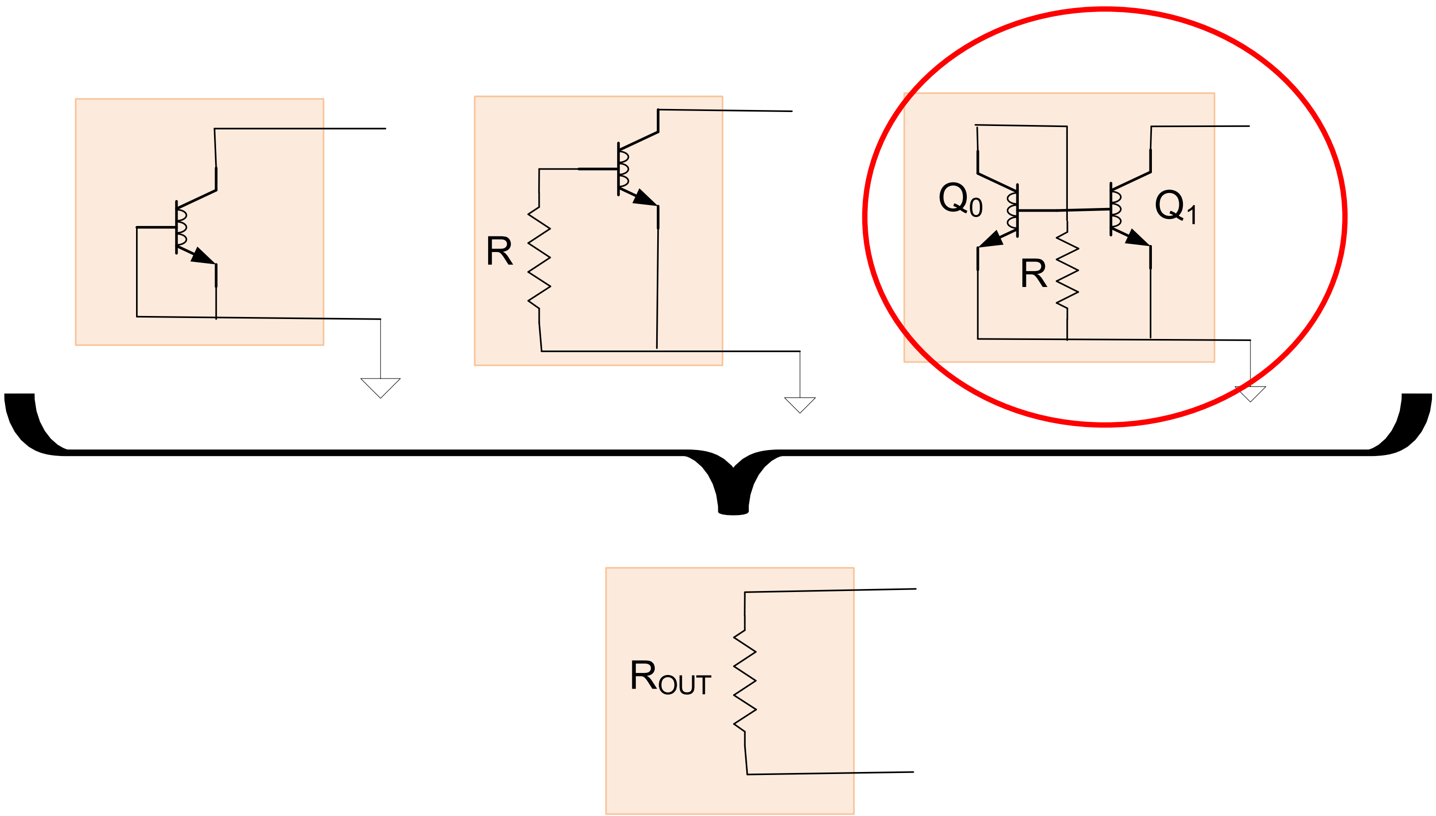
Basic Current Sources and Sinks

Small-signal Model of BJT Current Sinks and Sources



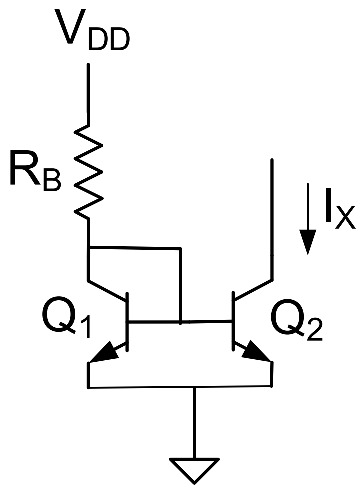
Basic Current Sources and Sinks

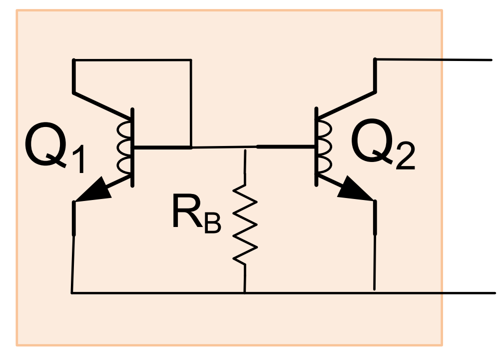
Small-signal Model of BJT Current Sinks and Sources



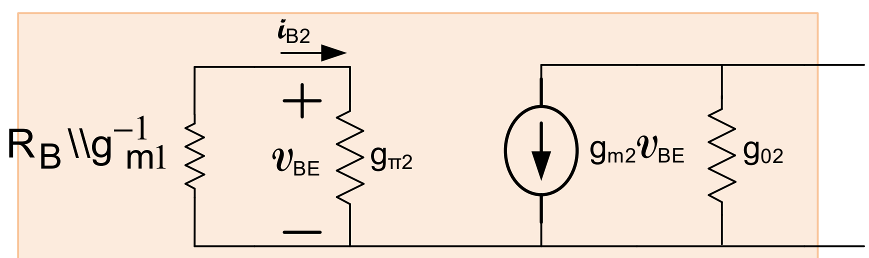
Basic Current Sources and Sinks

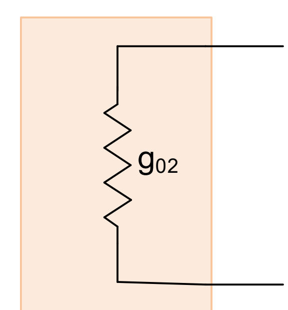
Small-signal Model of BJT Current Sinks and Sources





Small-signal of Q_1
Diode connected

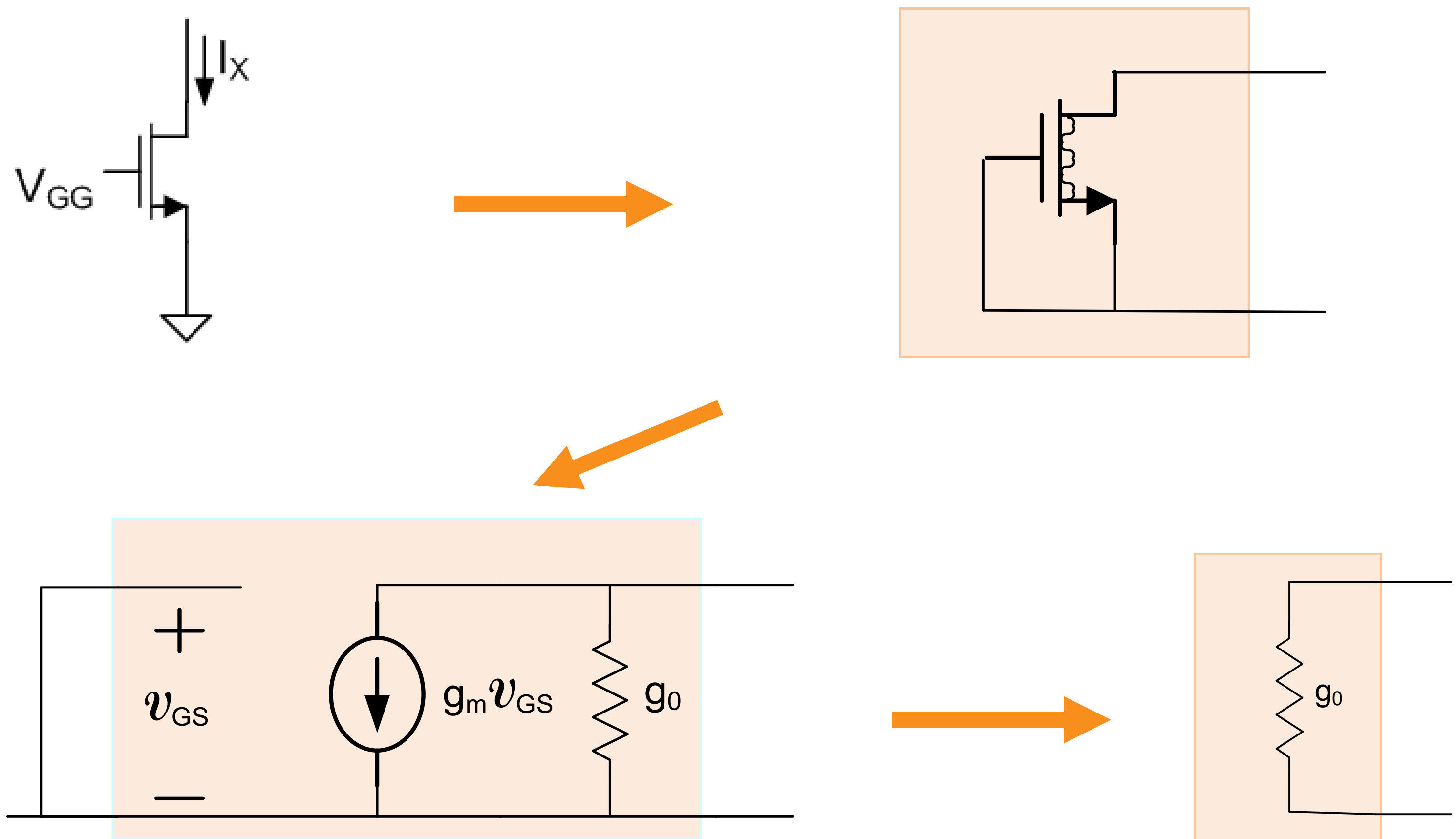




Small-signal model of all other BJT Sinks and Sources introduced so far are the same

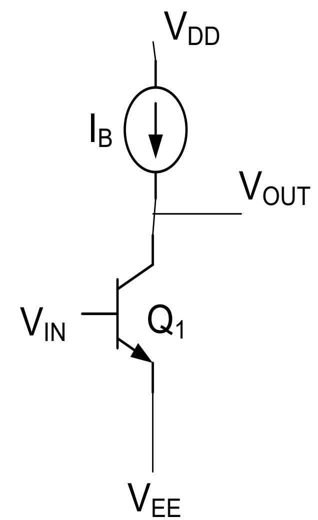
Basic Current Sources and Sinks

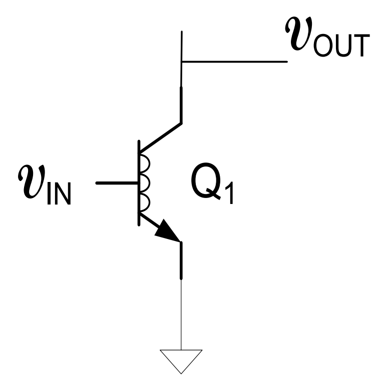
Small-signal Model of MOS Current Sinks and Sources



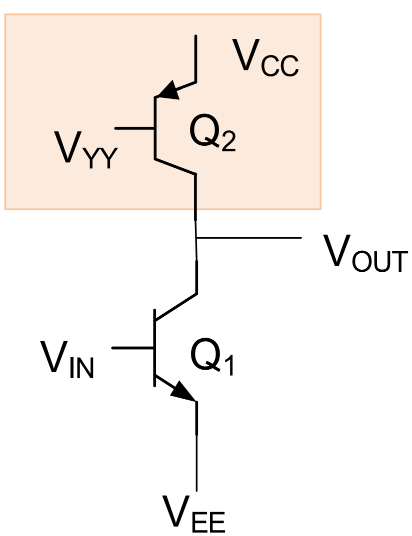
Small-signal model of all other MOS Sinks and Sources introduced thus far are the same

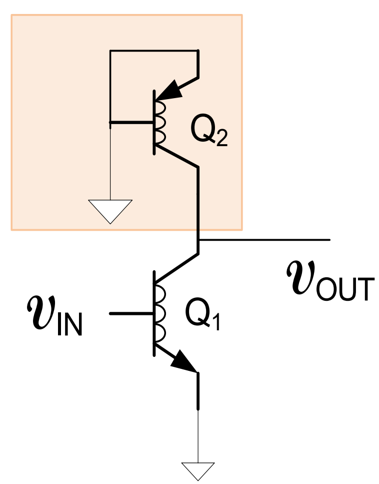
High-gain bipolar amplifier

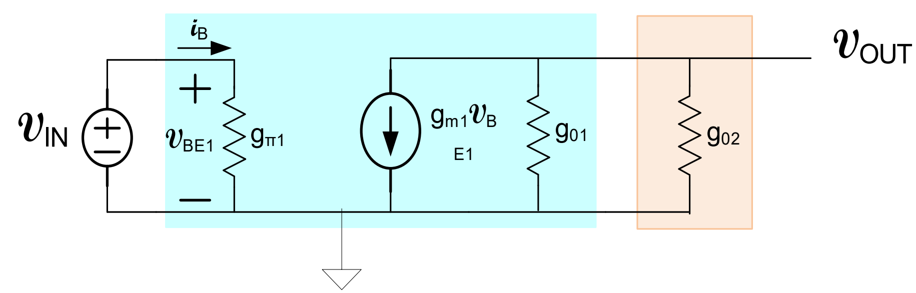




$$A_V = \frac{-g_m}{g_0}$$

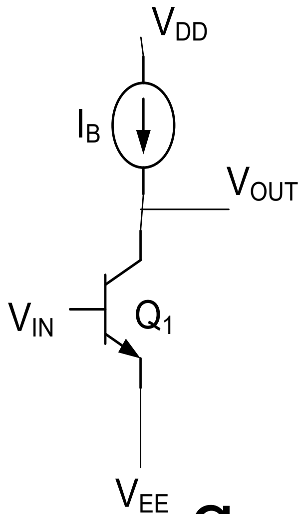




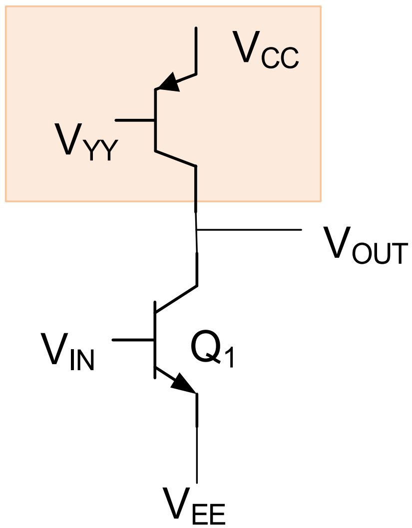


$$A_V = \frac{-g_{m1}}{g_{01} + g_{02}} \cong \frac{-g_{m1}}{2g_{01}}$$

High-gain amplifier



Recall: $\frac{g_m}{g_0} = \frac{g_{m1}}{g_{01}} = \frac{V_{AF}}{V_t} \cong 8000$



$$A_V = \frac{-g_m}{g_0} = -8000$$

$$A_V \cong \frac{-g_{m1}}{2g_{01}} = -4000$$

- **Nonideal current source decreased the gain by a factor of 2**
- **But the voltage gain is still quite large (-4000)**

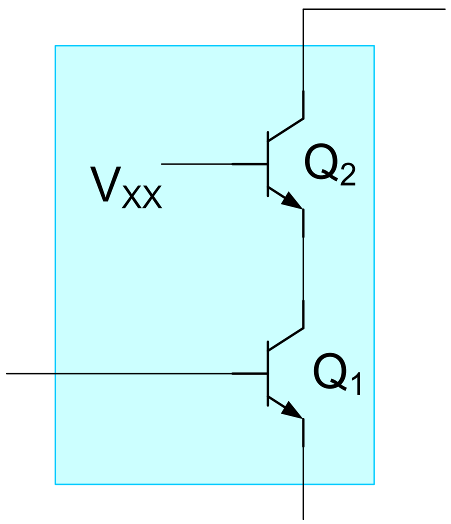
Can the gain be made even larger?

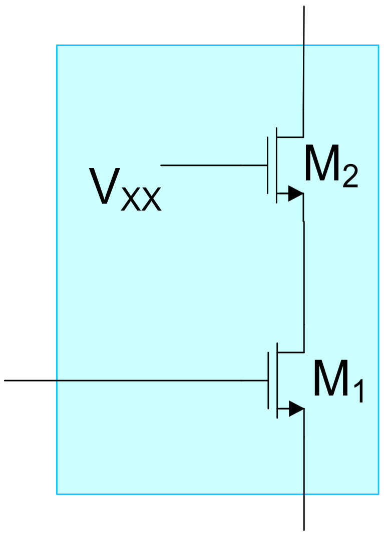
High-gain amplifier

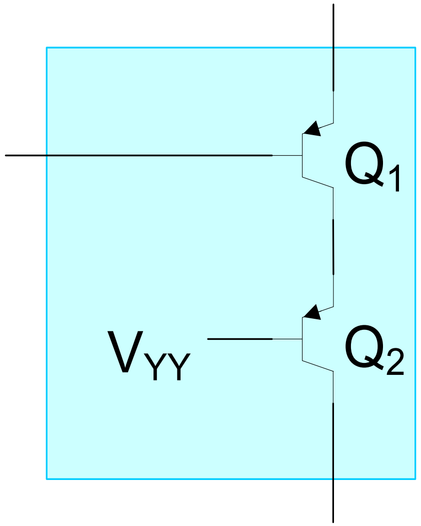
Can the gain be made even larger?

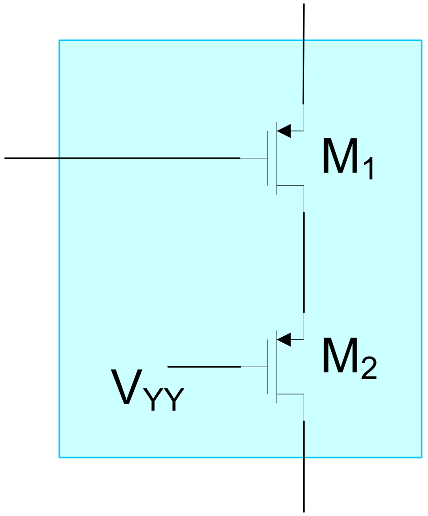
Discuss

The Cascode Configuration

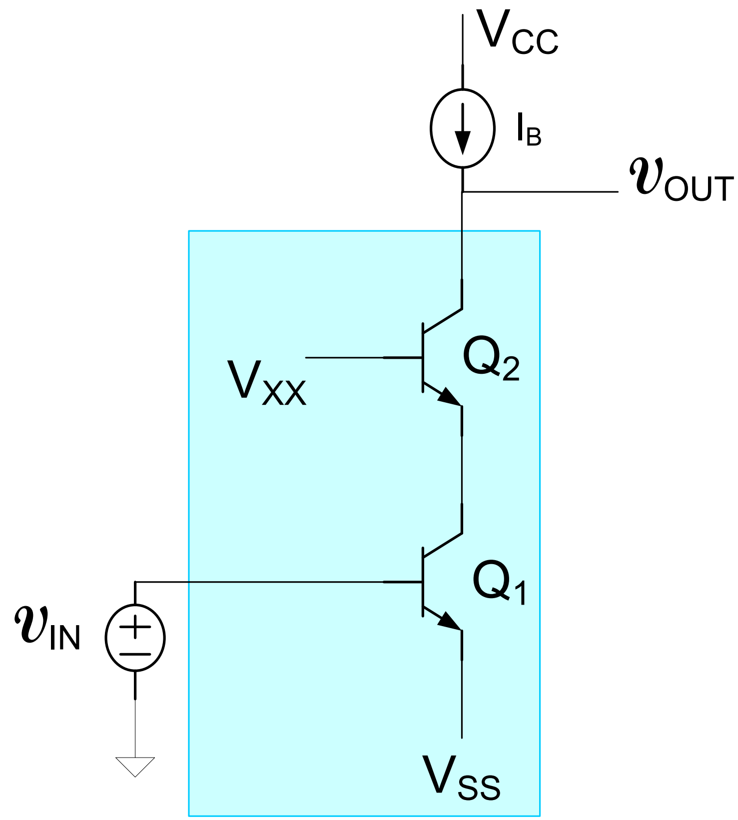








The Cascode Amplifier (consider npn BJT version)



Discuss

- **Actually a cascade of a CE stage followed by a CB stage but usually viewed as a "single-stage" structure**
- **Cascode structure is widely used**

Basic Amplifier Structures

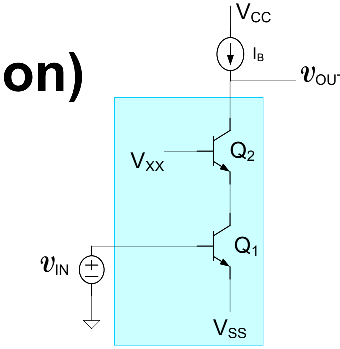
Discuss

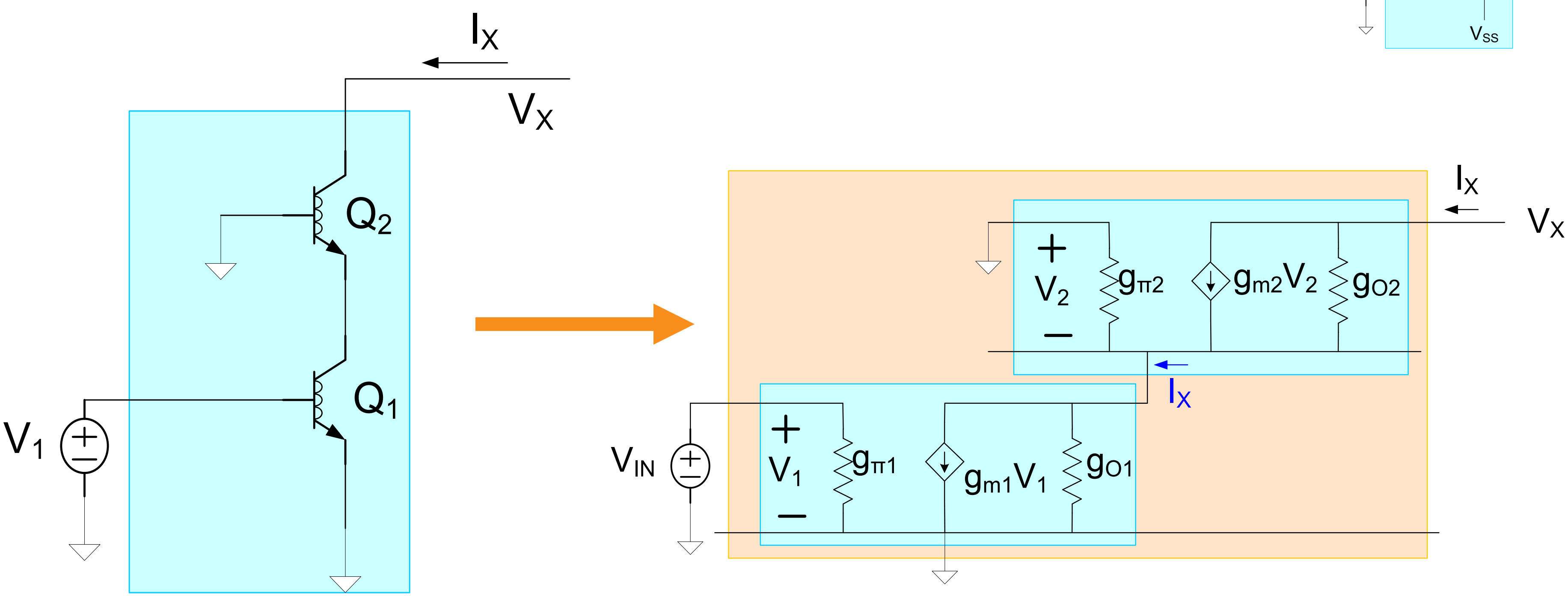
1. Common Emitter/Common Source
2. Common Collector/Common Drain
3. Common Base/Common Gate
4. Common Emitter with R_E/ Common Source with R_S

5. Cascode (actually CE:CB or CS:CD cascade)
6. Darlington (special CE:CE or CS:CS cascade)

The first 4 are most popular

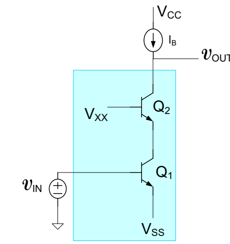
The Cascode Amplifier (consider npn BJT version)

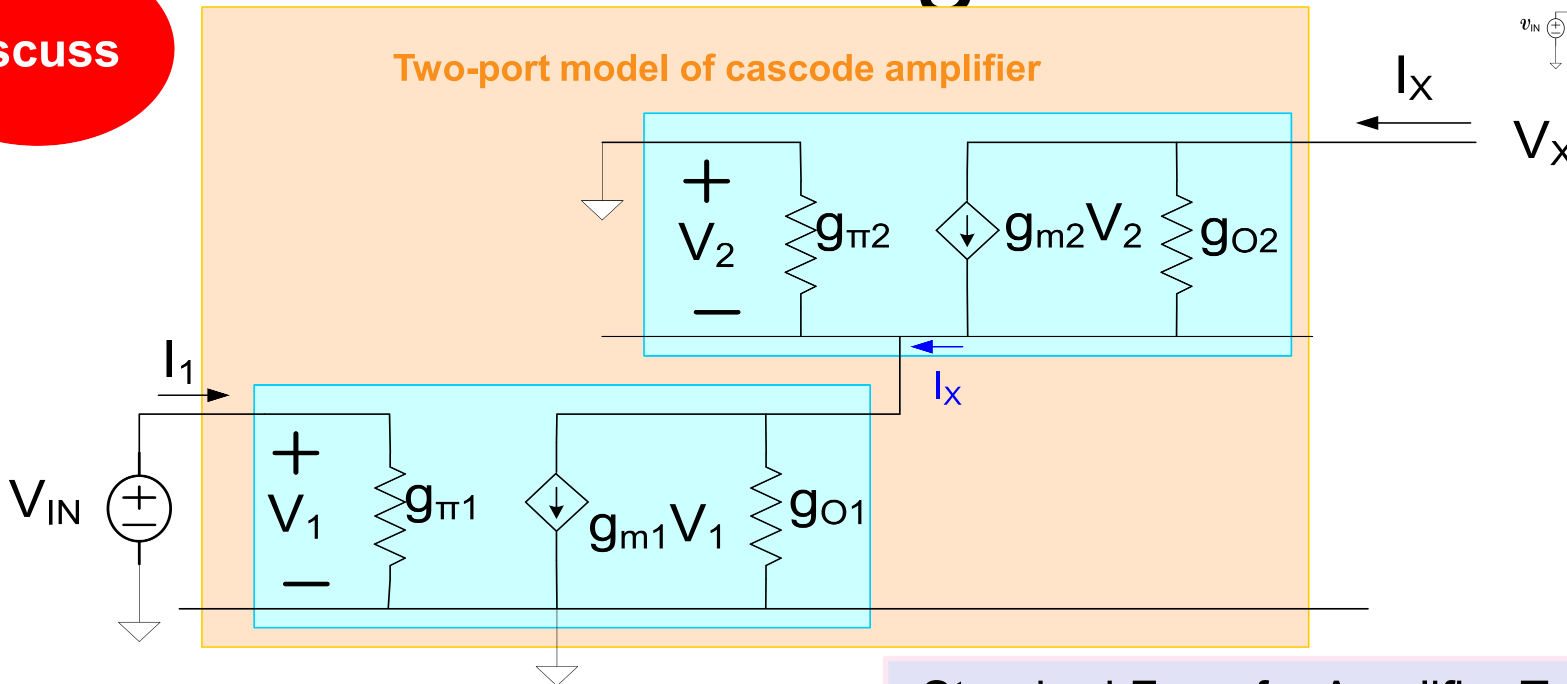




Cascode Configuration

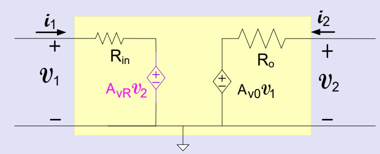
Discuss





$$\left.\begin{aligned}(V_X+V_2)g_{O2}+V_2 g_{m2}&=I_X\\ V_1\, g_{m1}-V_2\left(g_{O1}+g_{\pi 2}\right)&=I_X\end{aligned}\right\}$$

Standard Form for Amplifier Two-Port



$$v_1 = i_1 R_{IN} + A_{VR} v_2$$
$$v_2 = i_2 R_O + A_{V0} v_1$$

Observing V_1=V_{IN} and eliminating V_2 between these two equations, we obtain

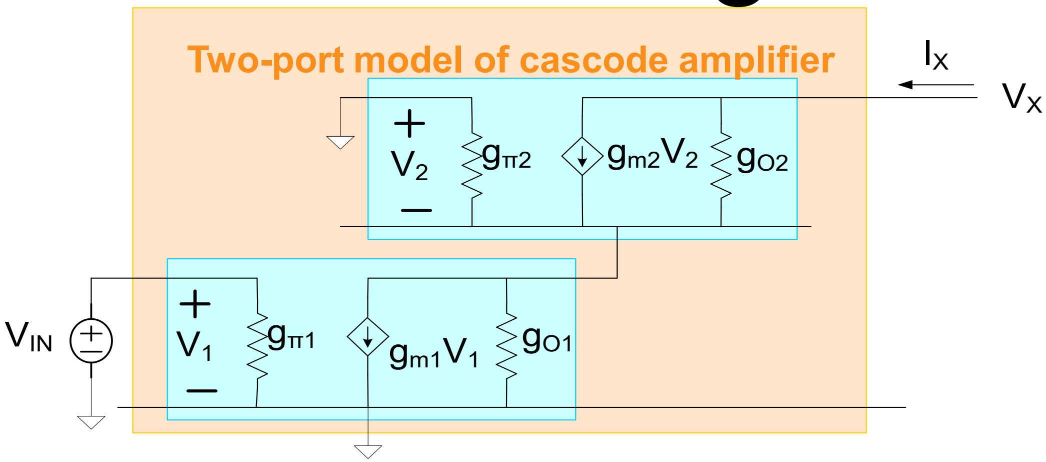
$$V_{IN}=I_1 \bullet \frac{1}{g_{\pi 1}}$$

and

$$V_X=I_X \bullet \left[\frac{g_{O1}+g_{O2}+g_{\pi 2}+g_{m2}}{g_{O2}\left(g_{O1}+g_{\pi 2}\right)}\right]-V_{IN} \bullet \left[\frac{g_{m1}\left(g_{O2}+g_{m2}\right)}{g_{O2}\left(g_{\pi 2}+g_{O1}\right)}\right]$$

Cascode Configuration

Discuss



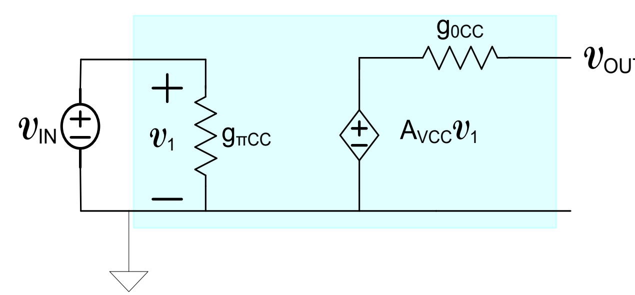
$$V_X = I_X \bullet \left[\frac{g_{01}+g_{02}+g_{\pi 2}+g_{m2}}{g_{02}\left(g_{01}+g_{\pi 2}\right)}\right] - V_{IN} \bullet \left[\frac{g_{m1}\left(g_{02}+g_{m2}\right)}{g_{02}\left(g_{\pi 2}+g_{01}\right)}\right]$$

$$V_{IN} = I_1 \bullet \frac{1}{g_{\pi 1}}$$

It thus follows for the npn bipolar structure that it is unilateral and :

$$A_{VCC} = -\left[\frac{g_{m1}\left(g_{02}+g_{m2}\right)}{g_{02}\left(g_{\pi 2}+g_{01}\right)}\right] \cong -\left[\frac{g_{m1}g_{m2}}{g_{02}g_{\pi 2}}\right]$$

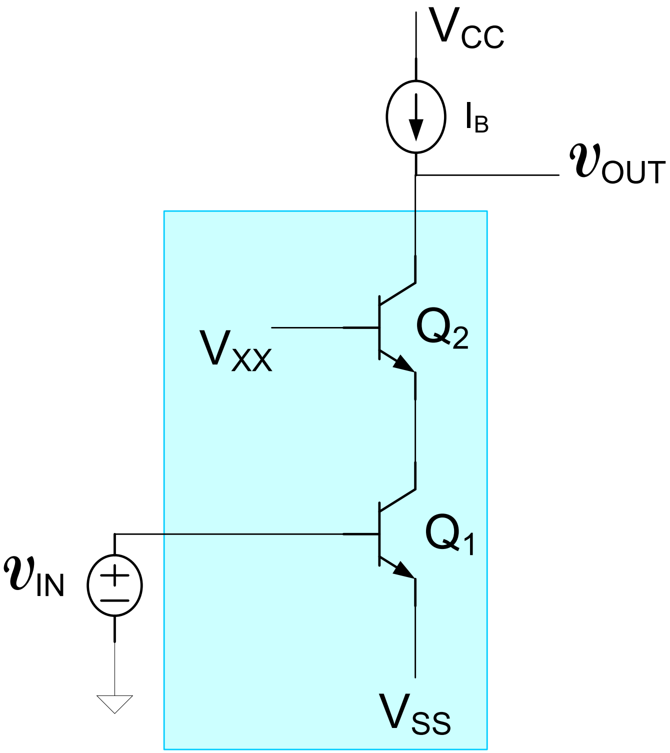
$$g_{0CC} = \left[\frac{g_{02}\left(g_{01}+g_{\pi 2}\right)}{g_{01}+g_{02}+g_{\pi 2}+g_{m2}}\right] \cong \left[\frac{g_{02}g_{\pi 2}}{g_{m2}}\right]$$



$$g_{\pi CC} = g_{\pi 1}$$

Cascode Configuration

Discuss



$$A_{VCC} \cong -\left[\frac{g_{m1}g_{m2}}{g_{02}g_{\pi 2}}\right]$$

$$g_{0CC} \cong \left[\frac{g_{02}g_{\pi 2}}{g_{m2}}\right]$$

$$g_{\pi CC} = g_{\pi 1}$$

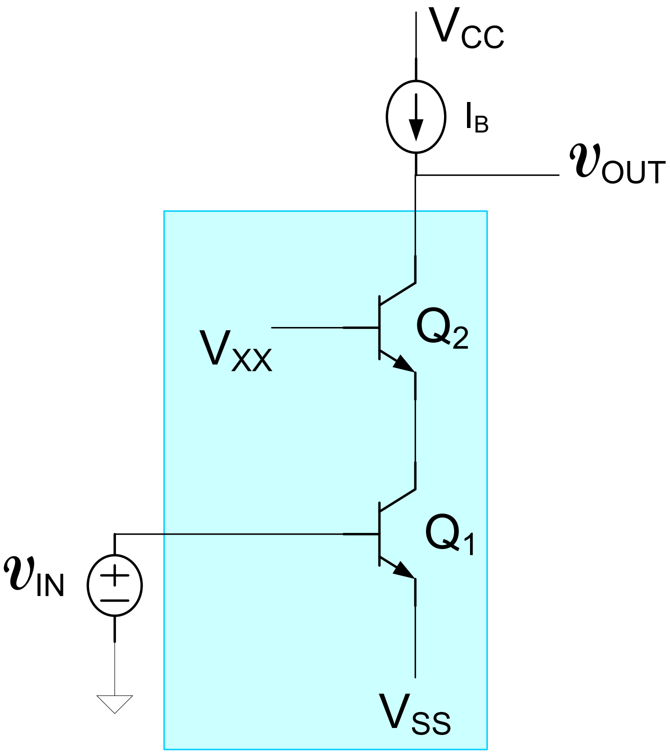
$$A_{VCC} \cong -\left[\frac{g_{m1}}{g_{02}}\beta\right] \cong -\left[\frac{g_{m1}}{g_{01}}\right]\beta$$

$$g_{0CC} \cong \frac{g_{01}}{\beta}$$

- **Voltage gain is a factor of β larger than that of the CE amplifier with current source load**
- **Output impedance is a factor of β larger than that of the CE amplifier**

Cascode Configuration

Discuss



$$A_{VCC} \cong -\left[\frac{g_{m1}}{g_{02}}\beta\right] \cong -\left[\frac{g_{m1}}{g_{01}}\right]\beta$$

$$g_{0CC} \cong \frac{g_{02}}{\beta}$$

In the MPOP domain:

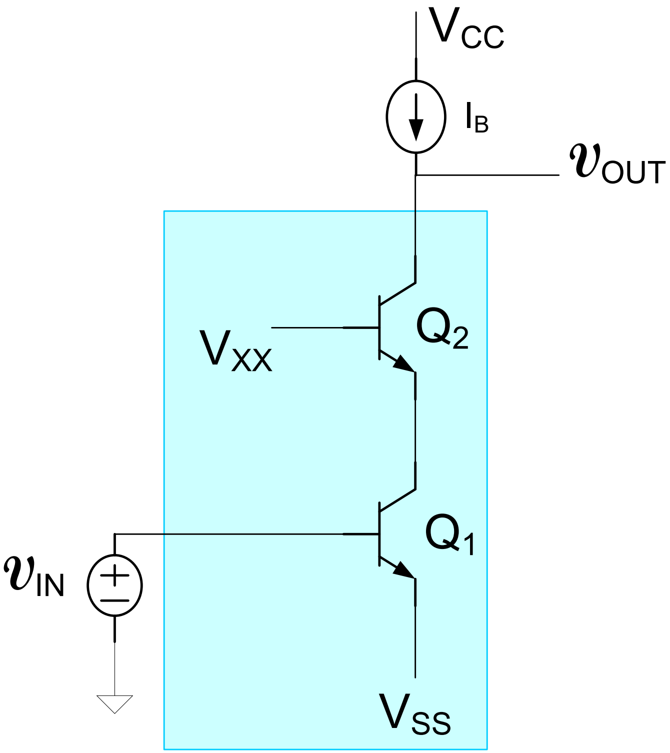
$$A_{VCC} \cong -\left[\frac{g_{m1}}{g_{01}}\right]\beta = \left[\frac{2V_{AF}}{V_t}\right]\beta = [-8000]100$$

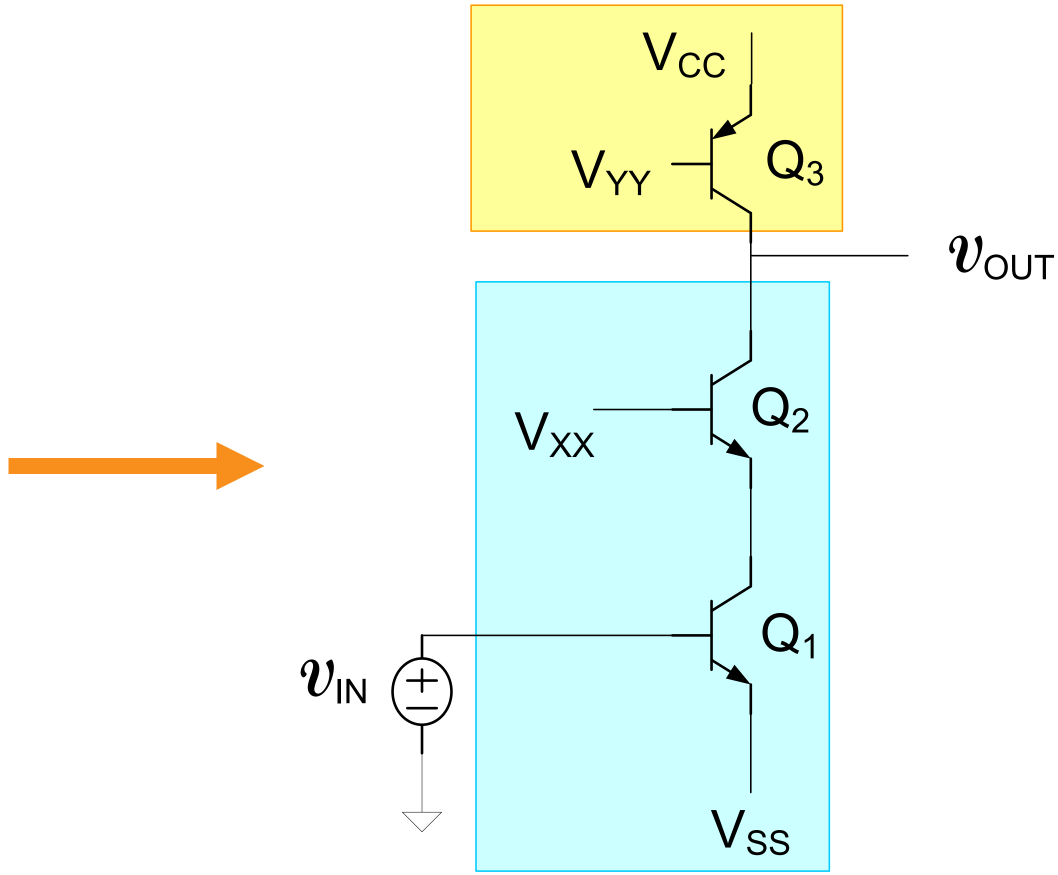
$$A_{VCC} \cong -800,000$$

This gain is very large and only requires two transistors!

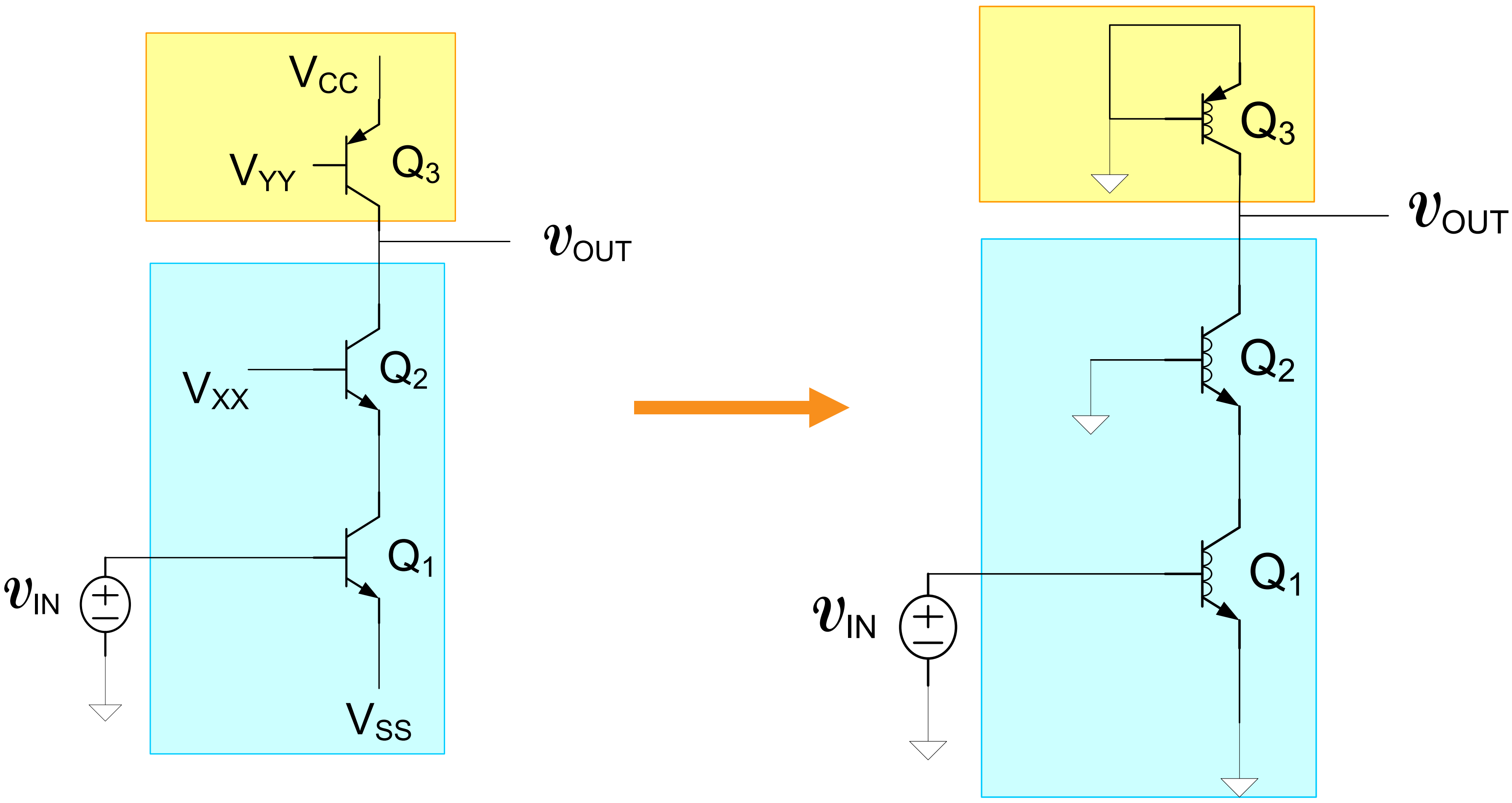
What happens to the gain if a transistor-level current source is used for I_B?

Cascode Configuration

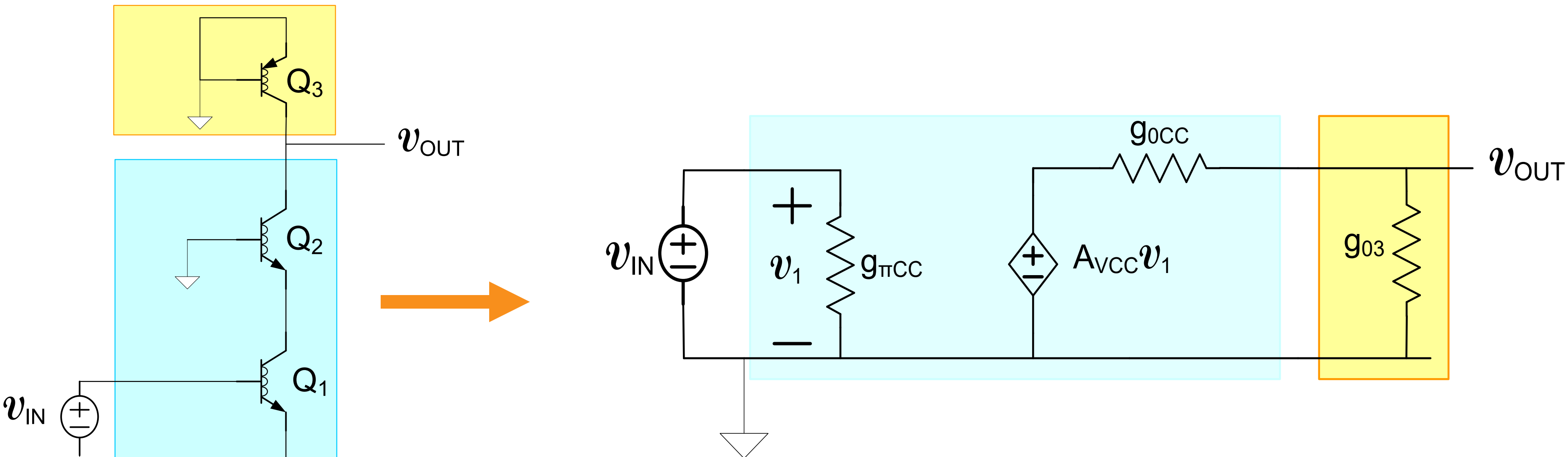




Cascode Configuration



High-gain amplifier comparisons



It thus follows that

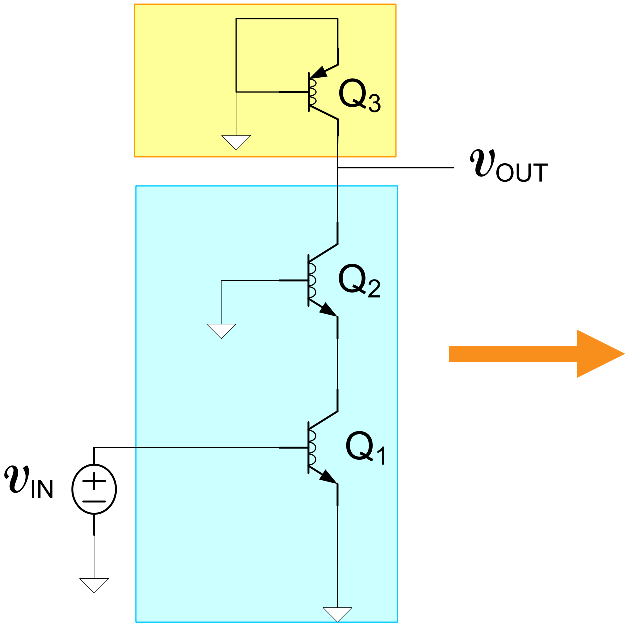
$$A_V = A_{VCC}\left[\frac{g_{0CC}}{g_{03}+g_{0CC}}\right]$$

But $\quad g_{0CC} \simeq g_{01}/\beta = g_{03}/\beta$

$$A_V \cong A_{VCC}\left[\frac{g_{0CC}}{g_{03}}\right] \cong \frac{A_{VCC}}{\beta}$$

This is a dramatic reduction in gain compared to what the ideal current source biasing provided

Cascode Configuration



$$A_V \cong A_{VCC}\left[\frac{g_{0CC}}{g_{03}}\right] \cong \frac{A_{VCC}}{\beta}$$

But recall

$$A_{VCC} \cong -\left[\frac{g_{m1}}{g_{01}}\right]\beta$$

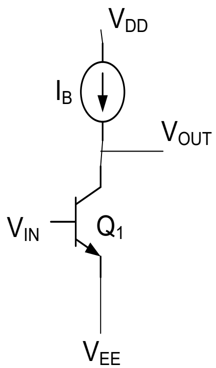
Thus $$A_V \cong -\left[\frac{g_{m1}}{g_{01}}\right]$$

In the MPOP domain:

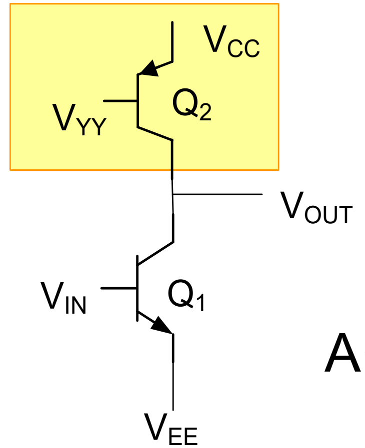
$$A_V \cong -\left[\frac{I_{CQ}/V_t}{I_{CQ}/V_{AF}}\right] = -\left[\frac{V_{AF}}{V_t}\right] \cong -8000$$

- **This is still a factor of 2 better than that of the CE amplifier with transistor current source** $\left(A_{VCE} \cong -\left[\frac{g_{m1}}{2g_{01}}\right]\right)$
- **It only requires one additional transistor**
- **But its not nearly as good as the gain the cascode circuit seemed to provide**

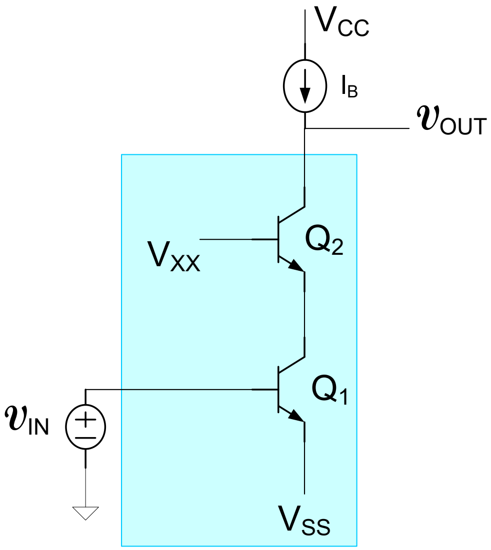
Cascode Configuration Comparisons



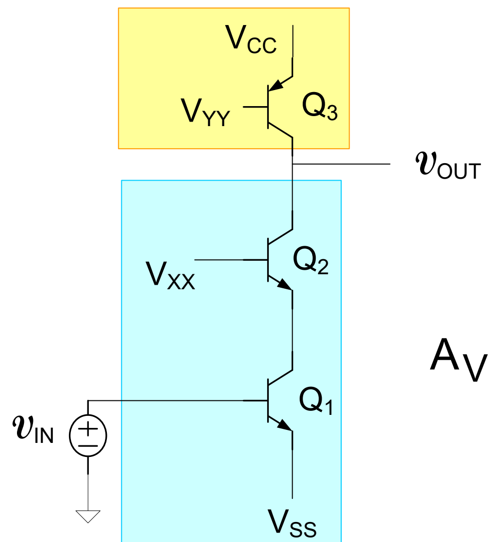
$$A_V = \frac{-g_m}{g_0}$$



$$A_V \cong \frac{-g_{m1}}{g_{01}+g_{02}} = \frac{-g_{m1}}{2g_{01}}$$



$$A_V \cong -\left[\frac{g_{m1}}{g_{01}}\right]\beta$$



$$A_V \cong -\left[\frac{g_{m1}}{\frac{g_{01}}{\beta}+g_{03}}\right] \cong -\left[\frac{g_{m1}}{g_{03}}\right]$$

Gain limited by output impedance of current scource !!

Can we design a better current source?

In particular, one with a higher output impedance?

Better current sources

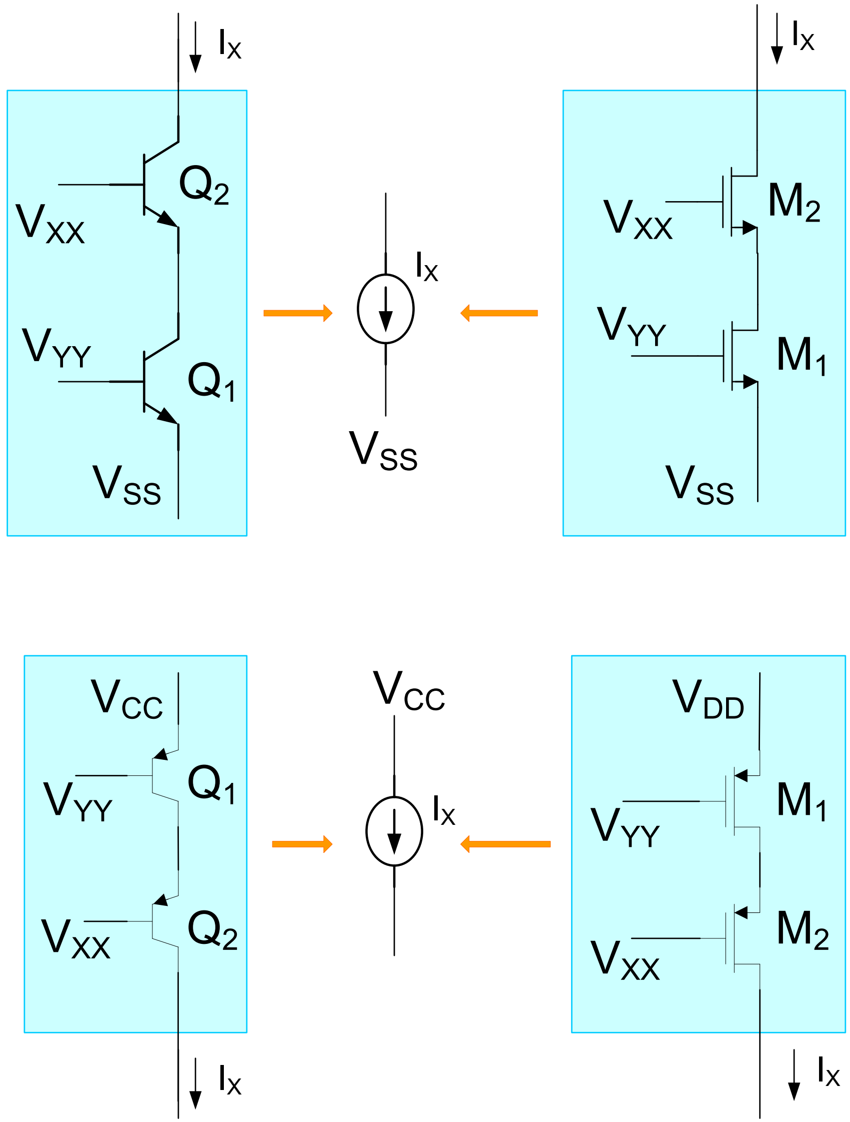
Need a higher output impedance than g_o

The output impedance of the cascode circuit itself was very large !

$$g_{0CC} \cong \frac{g_{01}}{\beta}$$

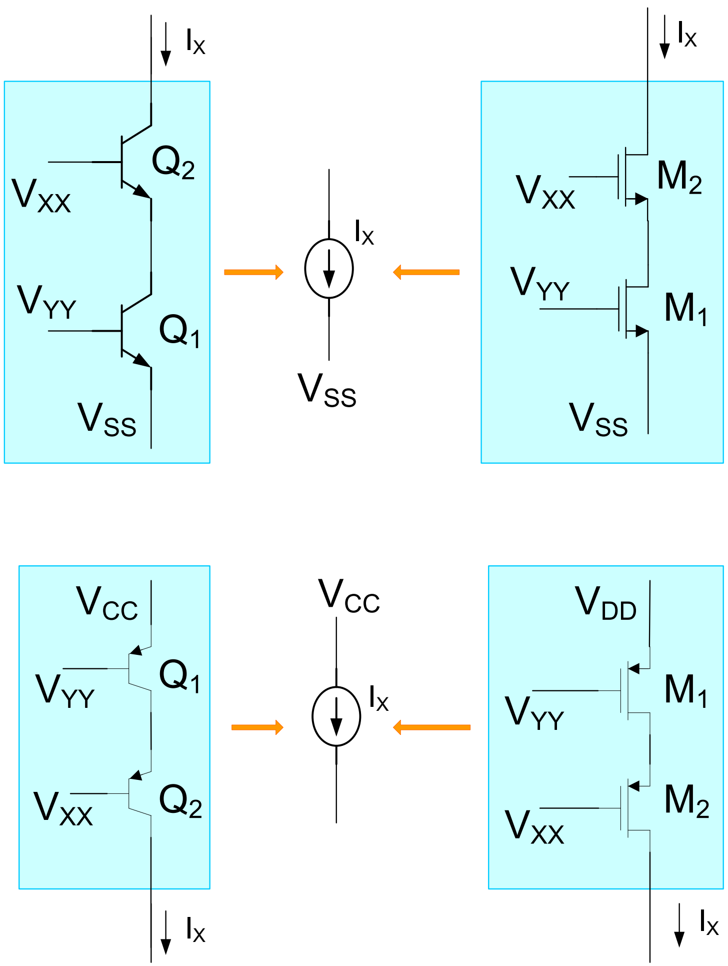
Can a current source be built with the cascode circuit ?

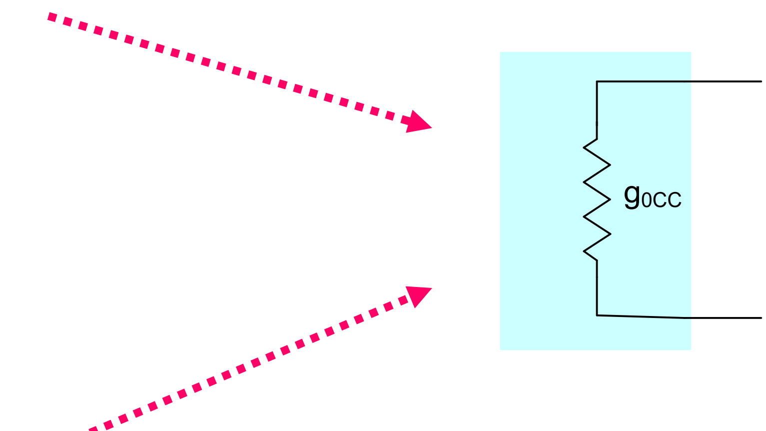
Cascode current sources



Discuss

Cascode current sources

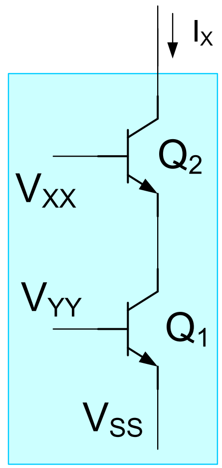


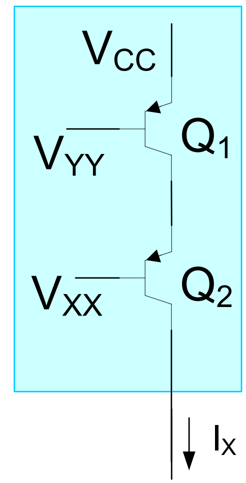


All have the same small-signal model

$$g_{0CC} = \left[\frac{g_{02}\left(g_{01}+g_{\pi 2}\right)}{g_{01}+g_{02}+g_{\pi 2}+g_{m2}} \right]$$

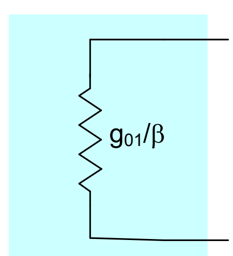
Cascode current sources



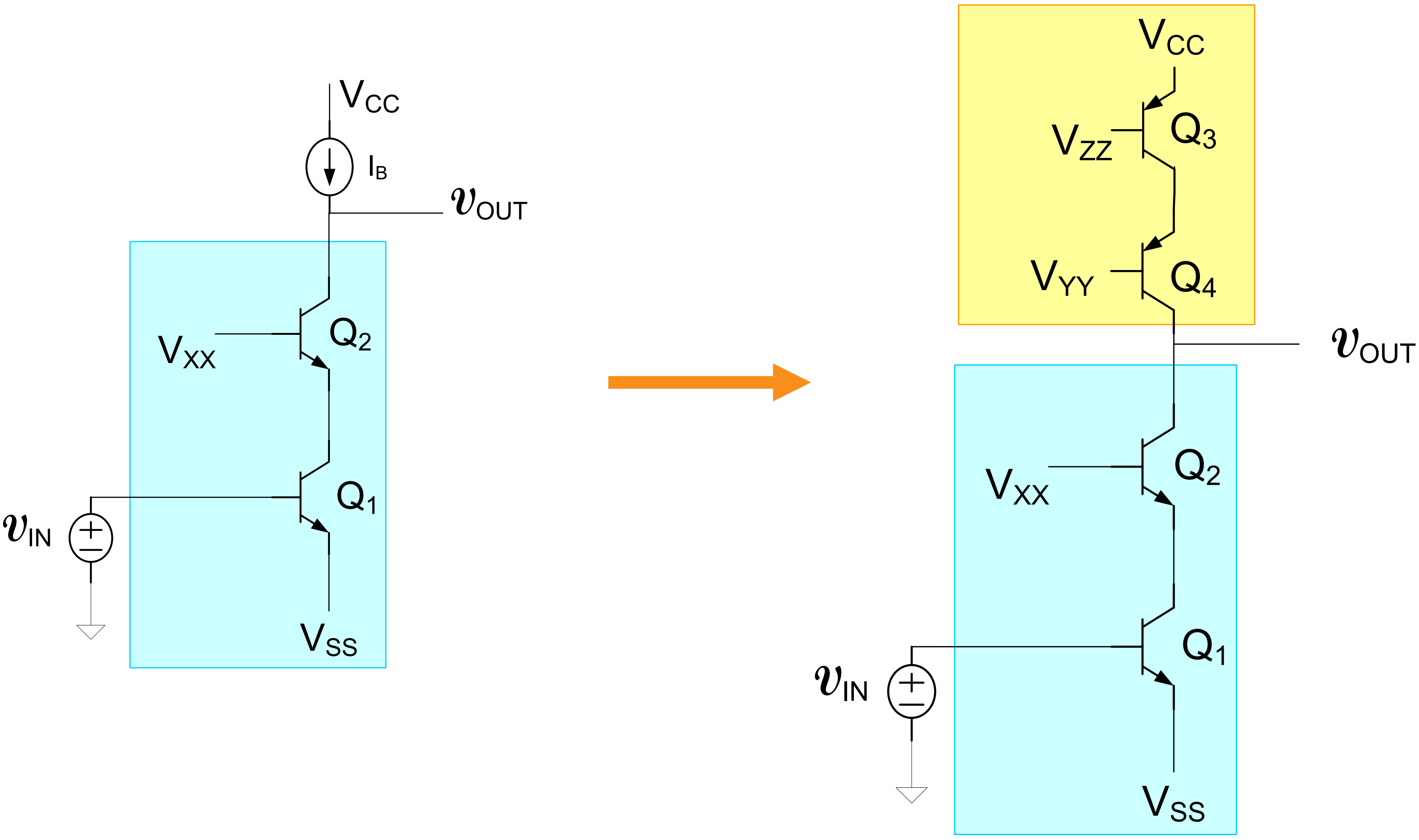


For the BJT cascode current sources

$$g_{0CC}=\left[\frac{g_{02}\left(g_{01}+g_{\pi 2}\right)}{g_{01}+g_{02}+g_{\pi 2}+g_{m2}}\right]\cong\left[\frac{g_{02}g_{\pi 2}}{g_{m2}}\right]=\frac{g_{01}}{\beta}$$

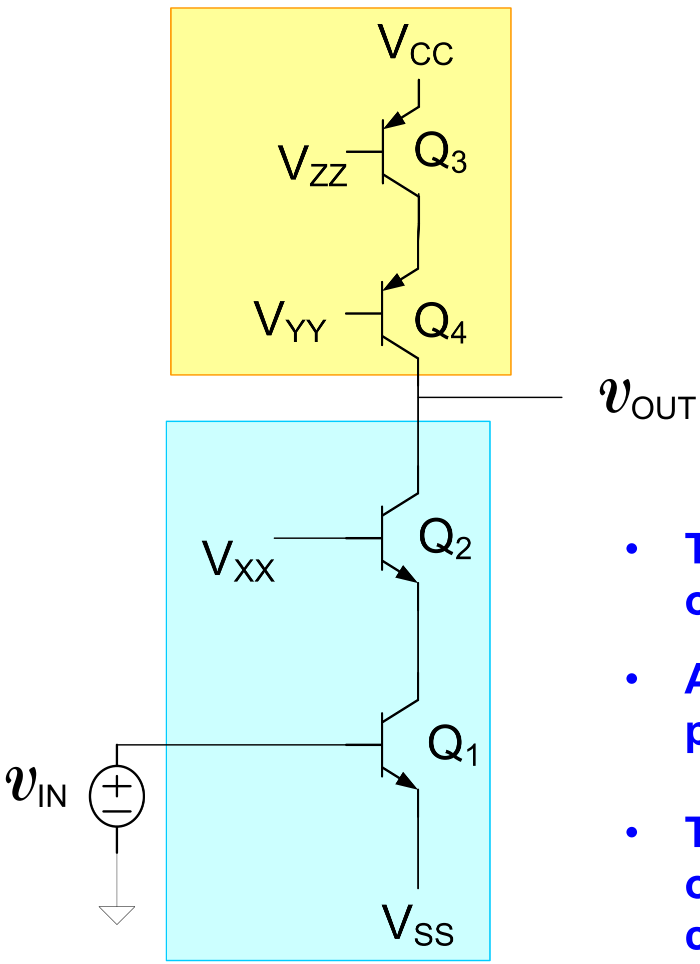


Cascode Configuration



Cascode Configuration

Discuss



$$A_V \cong -\left[\frac{g_{m1}}{\frac{g_{01}}{\beta_1}+g_{0CC}}\right] \cong -\left[\frac{g_{m1}}{\frac{g_{01}}{\beta_1}+\frac{g_{03}}{\beta_3}}\right]$$

If $\beta_1=\beta_3=\beta$

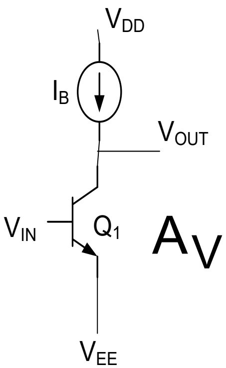
$$A_V = -\left[\frac{g_{m1}}{g_{01}}\right]\frac{\beta}{2}$$

$$A_V = -[8000]\frac{100}{2} \cong -400{,}000$$

- This gain is very large and is a factor of 2 below that obtained with an ideal current source biasing
- Although the factor of 2 is not desired, the performance of this circuit is still very good
- This factor of 2 gain reduction is that same as was observed for the CE amplifier when a transistor-level current source was used
- Biasing voltages V_{ZZ} and V_{SS} are critical so seldom used single-ended but good biasing strategies exist for differential operation

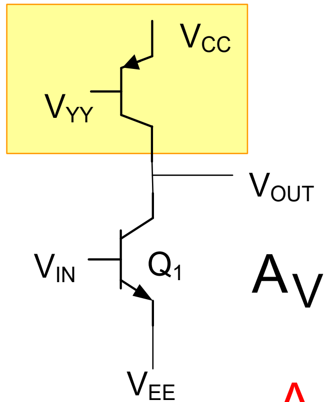
Cascode Configuration Comparisons

Discuss



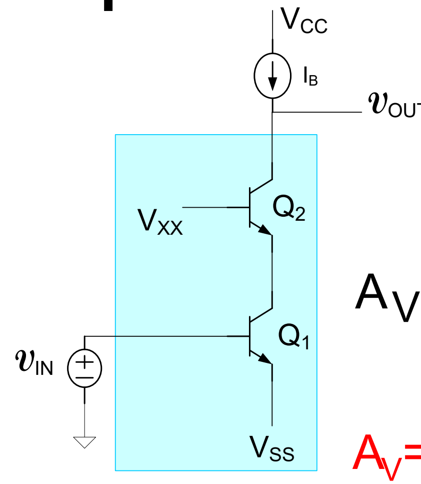
$$A_V = \frac{-g_m}{g_0}$$

$A_V = -8{,}000$



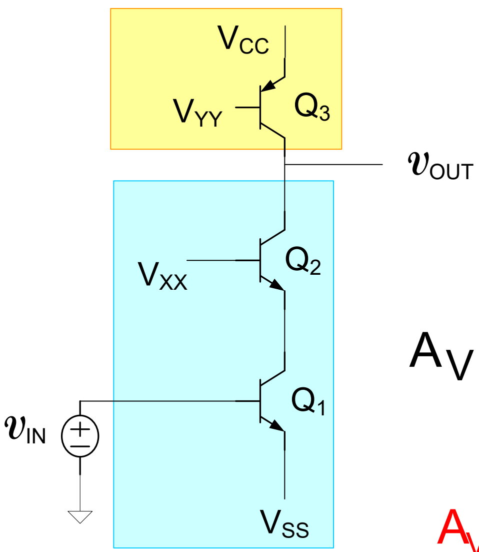
$$A_V \cong \frac{-g_{m1}}{2g_{01}}$$

$A_V = -4{,}000$



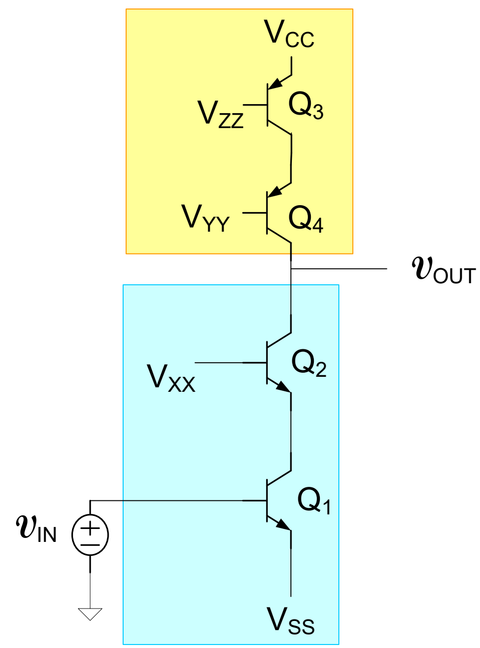
$$A_V \cong -\left[\frac{g_{m1}}{g_{01}}\right]\beta$$

$A_V = -800{,}000$



$$A_V \cong -\left[\frac{g_{m1}}{g_{01}}\right]$$

$A_V = -8{,}000$



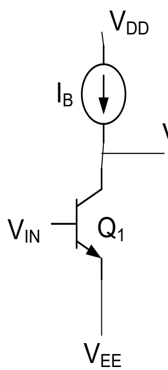
$$A_V = -\left[\frac{g_{m1}}{g_{01}}\right]\frac{\beta}{2}$$

$A_V = -400{,}000$

Can we use more cascoding to further increase the gain?

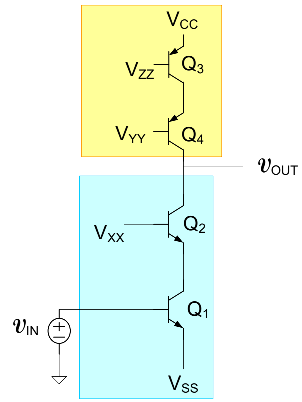
High Gain Amplifiers Seldom Used Open Loop

Discuss



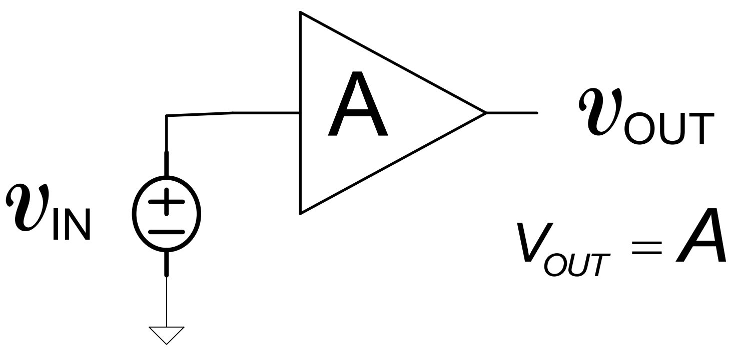
$$A_V = \frac{-g_m}{g_0}$$

A_V= -8,000



$$A_V = -\left[\frac{g_{m1}}{g_{01}}\right]\frac{\beta}{2}$$

A_V= -400,000



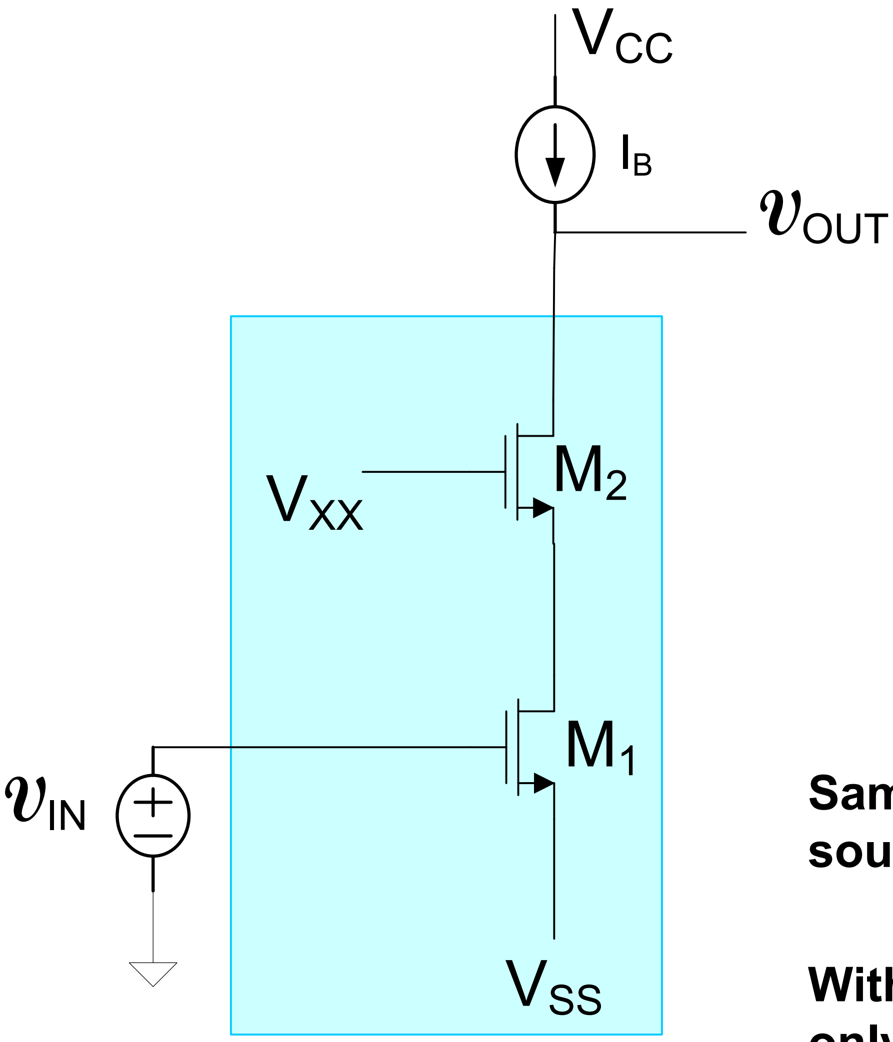
$$V_{OUT} = A\, v_{IN} + V_{OUTQ}$$

If A_V=-400,000 and V_{IN} increases by 1mV, what would happen at the output?

|V_{OUT} | would increase by 400,000 x 1mV=-400V

The Cascode Amplifier (consider n-ch MOS version)

Discuss



$$A_{VCC} \cong -\left[\frac{g_{m1}g_{m2}}{g_{01}g_{02}}\right]$$

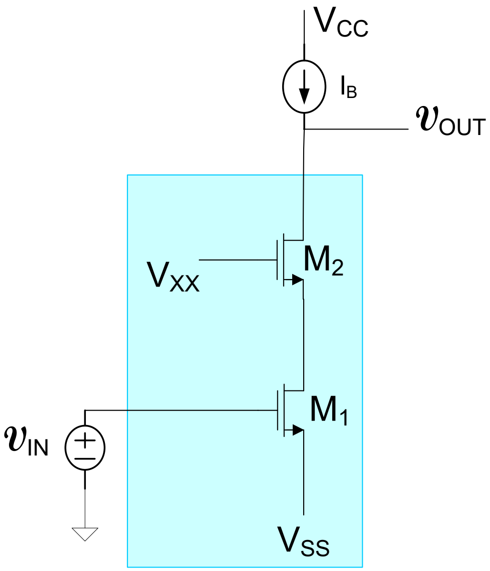
$$g_{0CC} \cong \left[\frac{g_{01}g_{02}}{g_{m2}}\right]$$

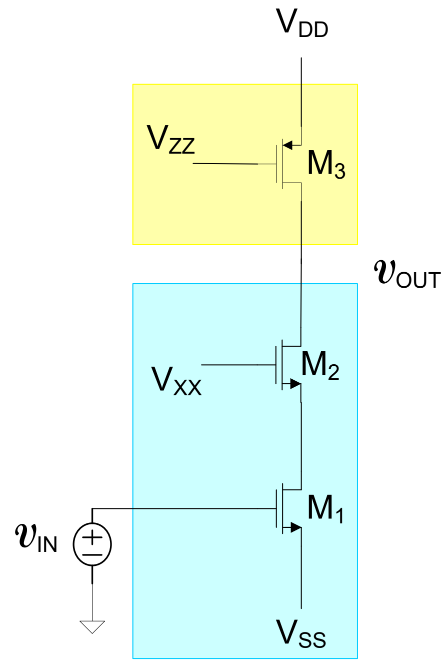
Same issues for biasing with current source as for BJT case

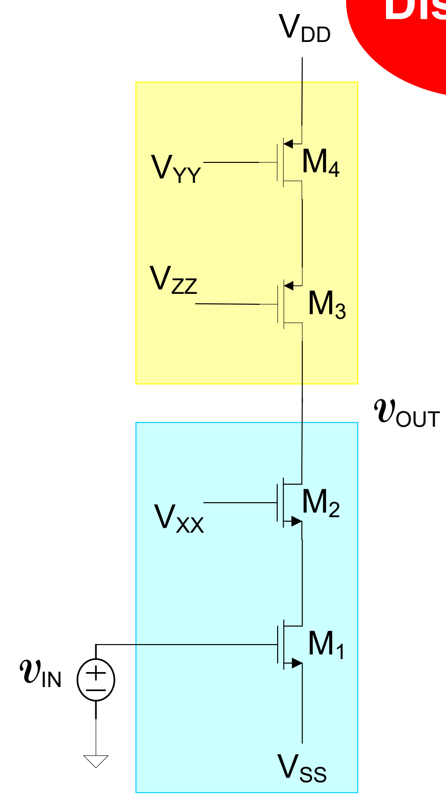
With cascode current source for I_B, gain only drops by a factor of 2 from value with ideal current source

The Cascode Amplifier (consider n-ch MOS version)

Discuss







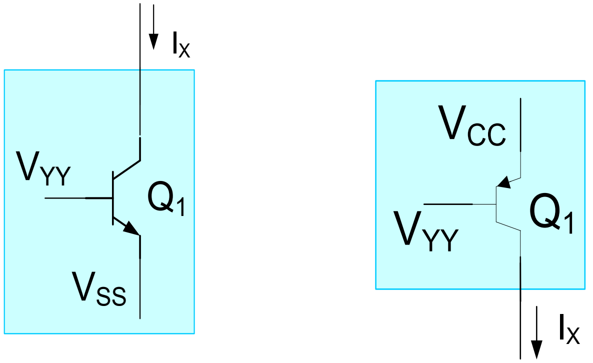
$$A_{VCC} \cong -\left[\frac{g_{m1}g_{m2}}{g_{01}g_{02}}\right]$$

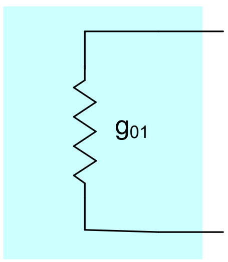
$$A_{VCC} \cong -\left[\frac{g_{m1}}{g_{01}}\right]$$

$$A_{VCC} \cong -\frac{1}{2}\left[\frac{g_{m1}g_{m2}}{g_{01}g_{02}}\right]$$

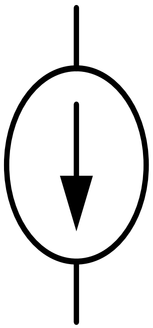
Current Source Summary (BJT)

Basic

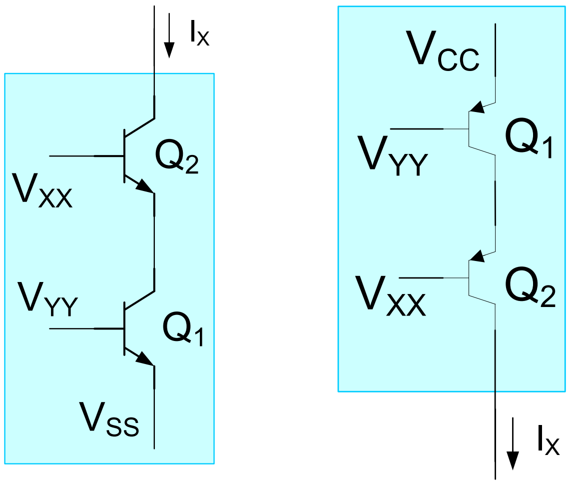


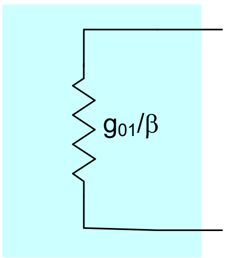


$$g_0 \cong g_{01}$$



Cascode

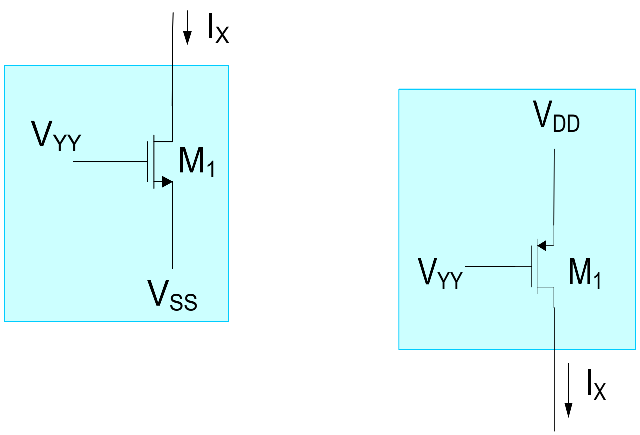


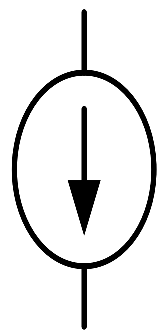


$$g_{0CC} \cong \frac{g_{01}}{\beta}$$

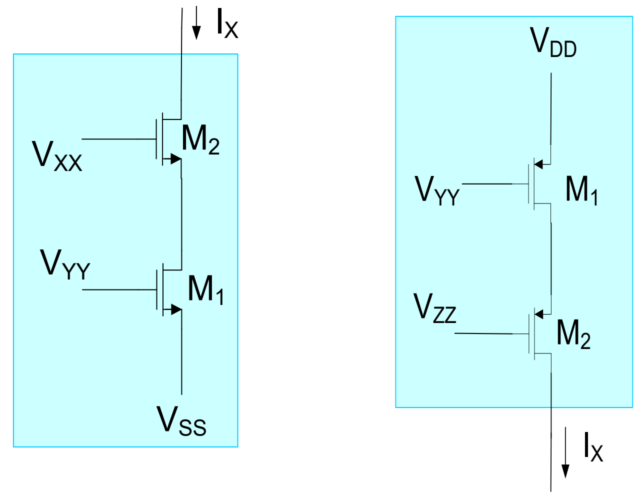
Current Source Summary (MOS)

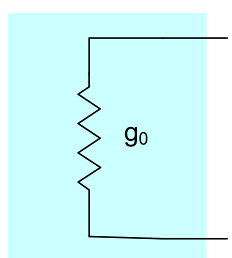
Basic



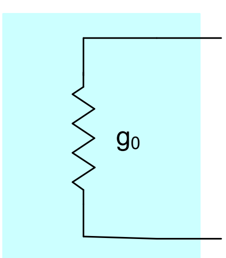


Cascode



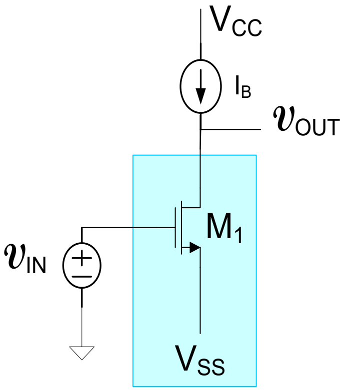


$$g_0 \cong g_{01}$$

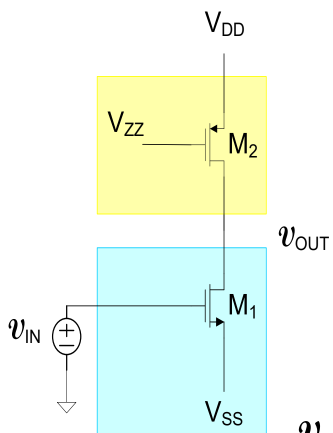


$$g_0 \cong g_{01}\frac{g_{02}}{g_{m2}}$$

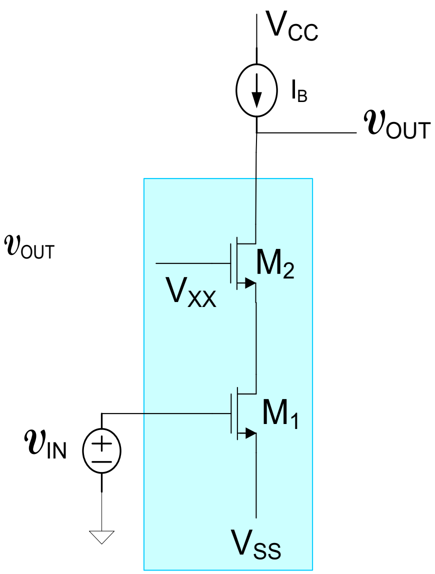
High Gain Amplifier Comparisons (n-ch MOS)



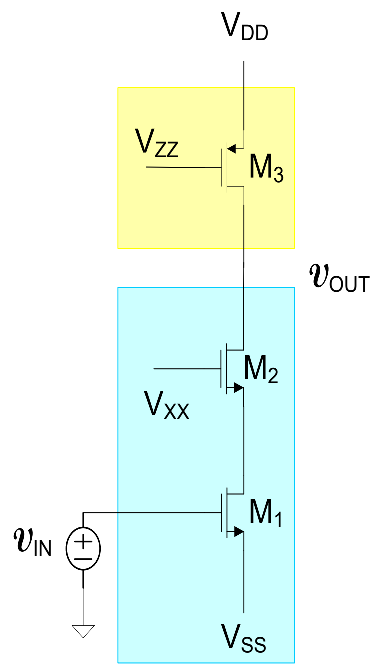
$$A_V \cong -\left[\frac{g_{m1}}{g_{01}}\right]$$



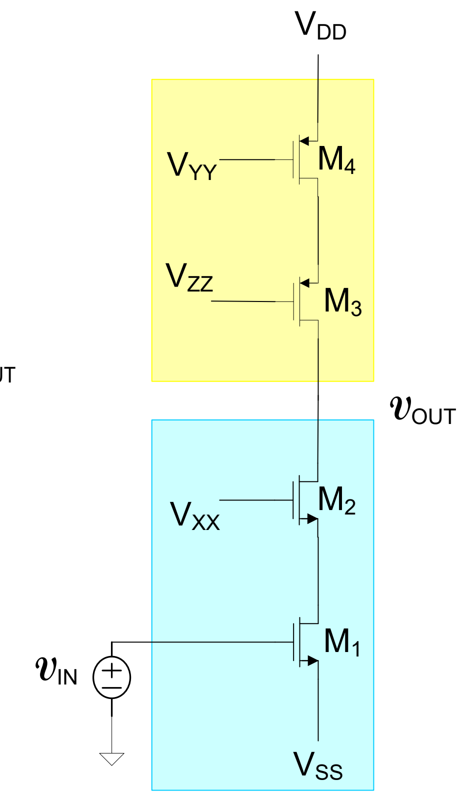
$$A_V \cong -\frac{1}{2}\left[\frac{g_{m1}}{g_{01}}\right]$$



$$A_{VCC} \cong -\left[\frac{g_{m1}g_{m2}}{g_{01}g_{02}}\right]$$

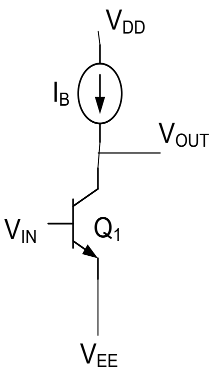


$$A_{VCC} \cong -\left[\frac{g_{m1}}{g_{01}}\right]$$

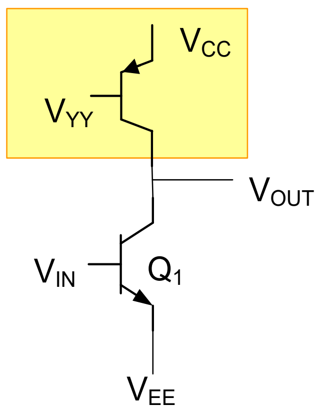


$$A_{VCC} \cong -\frac{1}{2}\left[\frac{g_{m1}g_{m2}}{g_{01}g_{02}}\right]$$

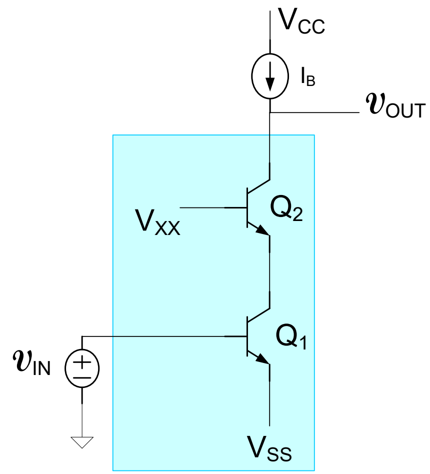
High Gain Amplifier Comparisons (BJT)



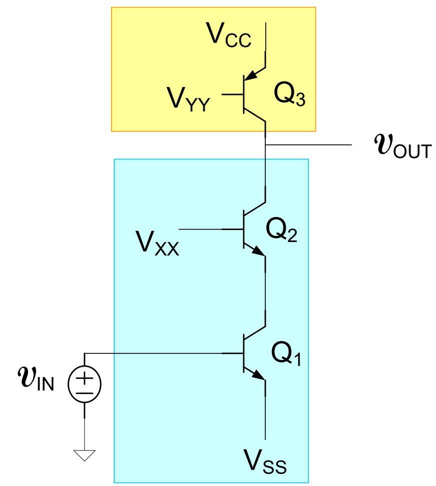
$$A_V = \frac{-g_m}{g_0}$$



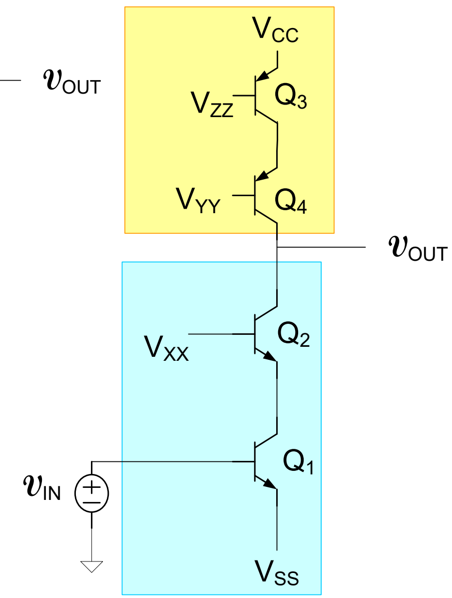
$$A_V \cong -\frac{1}{2}\frac{g_{m1}}{g_{01}}$$



$$A_V \cong -\left[\frac{g_{m1}}{g_{01}}\right]\beta$$



$$A_V \cong -\left[\frac{g_{m1}}{g_{01}}\right]$$



$$A_V = -\left[\frac{g_{m1}}{g_{01}}\right]\frac{\beta}{2}$$

- Single-ended high-gain amplifiers inherently difficult to bias (because of the high gain)
- Biasing becomes practical when used in differential applications
- These structures are widely used but usually with differential inputs

Stay Safe and Stay Healthy !

End of Lecture 34